



Chipsmall Limited consists of a professional team with an average of over 10 year of expertise in the distribution of electronic components. Based in Hongkong, we have already established firm and mutual-benefit business relationships with customers from,Europe,America and south Asia,supplying obsolete and hard-to-find components to meet their specific needs.

With the principle of "Quality Parts,Customers Priority,Honest Operation,and Considerate Service",our business mainly focus on the distribution of electronic components. Line cards we deal with include Microchip,ALPS,ROHM,Xilinx,Pulse,ON,Everlight and Freescale. Main products comprise IC,Modules,Potentiometer,IC Socket,Relay,Connector.Our parts cover such applications as commercial,industrial, and automotives areas.

We are looking forward to setting up business relationship with you and hope to provide you with the best service and solution. Let us make a better world for our industry!



Contact us

Tel: +86-755-8981 8866 Fax: +86-755-8427 6832

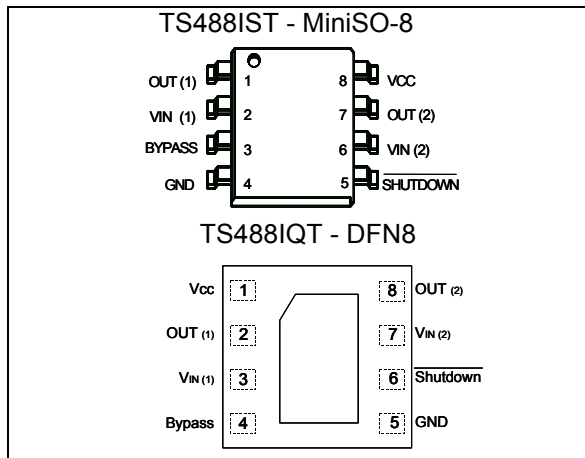
Email & Skype: info@chipsmall.com Web: www.chipsmall.com

Address: A1208, Overseas Decoration Building, #122 Zhenhua RD., Futian, Shenzhen, China



Pop-free 120 mW stereo headphone amplifier

Datasheet - production data



Description

The TS488/9 is an enhancement of TS486/7 that eliminates pop and click noise and reduces the number of external passive components.

The TS488/9 is a dual audio power amplifier capable of driving, in single-ended mode, either a 16 Ω or a 32 Ω stereo headset.

Capable of descending to low voltages, it delivers up to 31 mW per channel (into 16 Ω loads) of continuous average power with 0.1% THD+N in the audio bandwidth from a 2.5 V power supply.

An externally-controlled standby mode reduces the supply current to 10 nA (typ.). The unity gain stable TS488/9 is configured by external gain-setting resistors.

Features

- Pop and click noise protection circuitry
- Operating range from $V_{CC} = 2.2$ V to 5.5 V
- Standby mode active low (TS488) or high (TS489)
- Output power:
 - 120 mW at 5 V, into 16 Ω with 0.1% THD+N max (1 kHz)
 - 55 mW at 3.3 V, into 16 Ω with 0.1% THD+N max (1 kHz)
- Low current consumption: 2.7 mA max at 5 V
- Ultra-low standby current consumption: 10 nA typical
- High signal-to-noise ratio
- High crosstalk immunity: 102 dB ($F = 1$ kHz)
- PSRR: 70 dB typ. ($F = 1$ kHz), inputs grounded at 5 V
- Unity-gain stable
- Short-circuit protection circuitry
- Available in lead-free MiniSO-8 & DFN8 (2 x 2 mm)

Applications

- Headphone amplifiers
- Mobile phones, PDAs, computer motherboards
- High-end TVs, portable audio players

Contents

- 1 Typical application schematic 3**
- 2 Absolute maximum ratings and operating conditions 4**
- 3 Electrical characteristics 5**
- 4 Application information 22**
 - 4.1 Power dissipation and efficiency 22
 - 4.2 Total power dissipation 23
 - 4.3 Lower cutoff frequency 23
 - 4.4 Higher cutoff frequency 24
 - 4.5 Gain setting 25
 - 4.6 Decoupling of the circuit 25
 - 4.7 Standby mode 25
 - 4.8 Wake-up time 26
 - 4.9 POP performance 26
 - 4.10 Connecting the headphones 27
- 5 Package information 28**
 - 5.1 MiniSO-8 package information 29
 - 5.2 DFN8 package information 30
- 6 Ordering information 31**
- 7 Revision history 32**

1 Typical application schematic

Figure 1. Typical application for the TS488-TS489

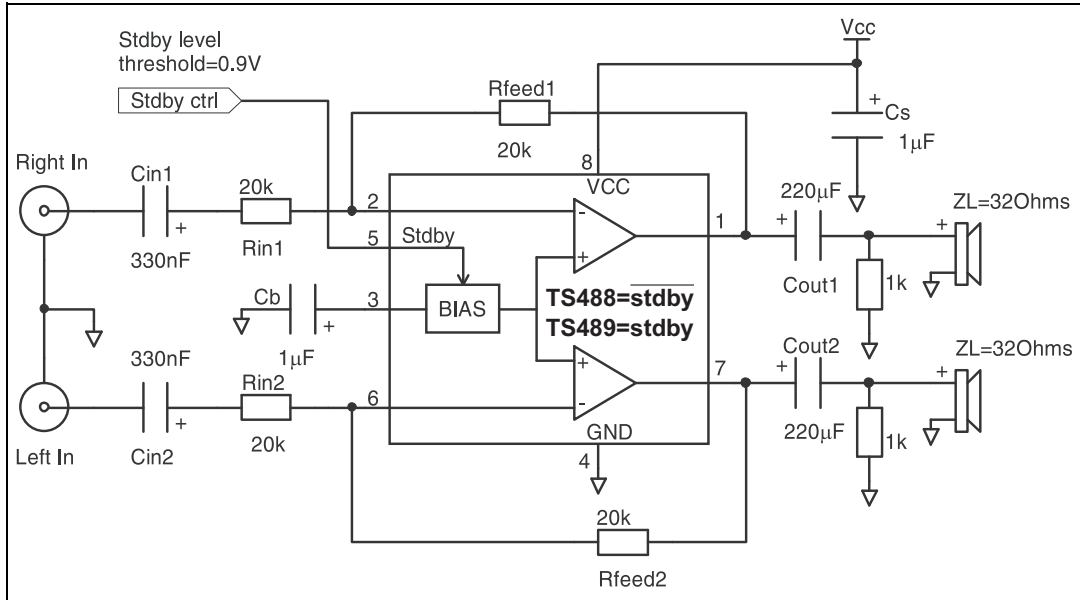


Table 1. Application component information

Component	Functional description
R _{in1,2}	Inverting input resistor that sets the closed loop gain in conjunction with R _{feed} . This resistor also forms a high pass filter with C _{in} ($F_c = 1 / (2 \times \text{Pi} \times R_{in} \times C_{in})$).
C _{in1,2}	Input coupling capacitor that blocks the DC voltage at the amplifier's input terminal.
R _{feed1,2}	Feedback resistor that sets the closed loop gain in conjunction with R _{in} . $A_V = \text{Closed Loop Gain} = -R_{feed}/R_{in}$.
C _s	Supply output capacitor that provides power supply filtering.
C _b	Bypass capacitor that provides half supply filtering.
C _{out1,2}	Output coupling capacitor that blocks the DC voltage at the load input terminal. This capacitor also forms a high pass with R _L ($F_c = 1 / (2 \times \text{Pi} \times R_L \times C_{out})$).

2 Absolute maximum ratings and operating conditions

Table 2. Absolute maximum ratings

Symbol	Parameter	Value	Unit
V_{CC}	Supply voltage ⁽¹⁾	6	V
V_i	Input voltage	-0.3 V to $V_{CC} + 0.3$ V	V
T_{stg}	Storage temperature	-65 to +150	°C
T_j	Maximum junction temperature	150	°C
R_{thja}	Thermal resistance junction-to-ambient		°C/W
	MiniSO-8 DFN8	215 70	
P_{diss}	Power dissipation ⁽²⁾ :		W
	MiniSO-8 DFN8	0.58 1.79	
ESD	Human body model (pin-to-pin)	2	kV
ESD	Machine model 220 pF - 240 pF (pin-to-pin)	200	V
Latch-up	Latch-up immunity (all pins)	200	mA
	Lead temperature (soldering, 10 sec)	250	°C
	Output short-circuit to V_{CC} or GND	continuous ⁽³⁾	

1. All voltage values are measured with respect to the ground pin.
2. P_{diss} is calculated with $T_{amb} = 25$ °C, $T_j = 150$ °C.
3. Attention must be paid to continuous power dissipation ($V_{DD} \times 250$ mA). Short-circuits can cause excessive heating and destructive dissipation. Exposing the IC to a short-circuit for an extended period of time will dramatically reduce the product's life expectancy.

Table 3. Operating conditions

Symbol	Parameter	Value	Unit
V_{CC}	Supply voltage	2.2 to 5.5	V
R_L	Load resistor	≥ 16	Ω
T_{oper}	Operating free air temperature range	-40 to + 85	°C
C_L	Load capacitor:		pF
	$R_L = 16$ to 100Ω $R_L > 100 \Omega$	400 100	
V_{STBY}	Standby voltage input: TS488 active, TS489 in standby TS488 in standby, TS489 active	$1.5 \leq V \leq V_{CC}$ $GND \leq V_{STBY} \leq 0.4$ ⁽¹⁾	V
R_{thja}	Thermal resistance junction-to-ambient		°C/W
	MiniSO-8 DFN8 ⁽²⁾	190 40	

1. The minimum current consumption (I_{STBY}) is guaranteed at GND (TS488) or V_{CC} (TS489) for the whole temperature range.
2. When mounted on a 4-layer PCB.

3 Electrical characteristics

**Table 4. Electrical characteristics at $V_{CC} = +5\text{ V}$
with $GND = 0\text{ V}$, $T_{amb} = 25\text{ °C}$ (unless otherwise specified)**

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
I_{CC}	Supply current	No input signal, no load		2	2.7	mA
I_{STBY}	Standby current	No input signal, $V_{STBY} = GND$ for TS488, $R_L = 32\ \Omega$		10	1000	nA
		No input signal, $V_{STBY} = V_{CC}$ for TS489, $R_L = 32\ \Omega$		10	1000	
P_{out}	Output power	THD+N = 0.1% max, $F = 1\text{ kHz}$, $R_L = 32\ \Omega$		75		mW
		THD+N = 1% max, $F = 1\text{ kHz}$, $R_L = 32\ \Omega$	70	80		
		THD+N = 0.1% max, $F = 1\text{ kHz}$, $R_L = 16\ \Omega$		120		
		THD+N = 1% max, $F = 1\text{ kHz}$, $R_L = 16\ \Omega$	100	130		
THD+N	Total harmonic distortion + noise	$A_V = -1$, $R_L = 32\ \Omega$, $P_{out} = 60\text{ mW}$, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		0.3		%
		$A_V = -1$, $R_L = 16\ \Omega$, $P_{out} = 90\text{ mW}$, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		0.3		
PSRR	Power supply rejection ratio, inputs grounded ⁽¹⁾	$A_V = -1$, $R_L \geq 16\ \Omega$, $C_b = 1\ \mu\text{F}$, $F = 1\text{ kHz}$, $V_{ripple} = 200\text{ mVpp}$	64	70		dB
		$A_V = -1$, $R_L \geq 16\ \Omega$, $C_b = 1\ \mu\text{F}$, $F = 217\text{ Hz}$, $V_{ripple} = 200\text{ mVpp}$	62	68		
V_O	Output swing	V_{OL} : $R_L = 32\ \Omega$		0.23	0.31	V
		V_{OH} : $R_L = 32\ \Omega$	4.53	4.72		
		V_{OL} : $R_L = 16\ \Omega$		0.44	0.57	
		V_{OH} : $R_L = 16\ \Omega$	4.18	4.48		
SNR	Signal-to-noise ratio	A-weighted, $A_V = -1$, $R_L = 32\ \Omega$, THD+N < 0.4%, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		105		dB
Crosstalk	Channel separation	$R_L = 32\ \Omega$, $A_V = -1$ $F = 1\text{ kHz}$ $F = 20\text{ Hz to } 20\text{ kHz}$		-102 -84		dB
C_i	Input capacitance			1		pF
GBP	Gain bandwidth product	$R_L = 32\ \Omega$		1.1		MHz
SR	Slew rate, unity gain inverting	$R_L = 16\ \Omega$		0.65		V/ μs
V_{IO}	Input offset voltage	$V_{icm} = V_{CC}/2$		1	20	mV
t_{wu}	Wake-up time			100		ms

1. Guaranteed by design and evaluation.

**Table 5. Electrical characteristics at $V_{CC} = +3.3\text{ V}$
with $GND = 0\text{ V}$, $T_{amb} = 25\text{ °C}$ (unless otherwise specified) ⁽¹⁾**

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
I_{CC}	Supply current	No input signal, no load		1.8	2.5	mA
I_{STBY}	Standby current	No input signal, $V_{STBY} = GND$ for TS488, $R_L = 32\ \Omega$		10	1000	nA
		No input signal, $V_{STBY} = V_{CC}$ for TS489, $R_L = 32\ \Omega$		10	1000	
P_{out}	Output power	THD+N = 0.1% max, $F = 1\text{ kHz}$, $R_L = 32\ \Omega$		34		mW
		THD+N = 1% max, $F = 1\text{ kHz}$, $R_L = 32\ \Omega$	30	35		
		THD+N = 0.1% max, $F = 1\text{ kHz}$, $R_L = 16\ \Omega$		55		
		THD+N = 1% max, $F = 1\text{ kHz}$, $R_L = 16\ \Omega$	47	57		
THD+N	Total harmonic distortion + noise	$A_V = -1$, $R_L = 32\ \Omega$, $P_{out} = 16\text{ mW}$, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		0.3		%
		$A_V = -1$, $R_L = 16\ \Omega$, $P_{out} = 35\text{ mW}$, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		0.3		
PSRR	Power supply rejection ratio, inputs grounded ⁽²⁾	$A_V = -1$, $R_L \geq 16\ \Omega$, $C_b = 1\ \mu\text{F}$, $F = 1\text{ kHz}$, $V_{ripple} = 200\text{ mVpp}$	63	69		dB
		$A_V = -1$, $R_L \geq 16\ \Omega$, $C_b = 1\ \mu\text{F}$, $F = 217\text{ Hz}$, $V_{ripple} = 200\text{ mVpp}$	61	67		
V_O	Output swing	V_{OL} : $R_L = 32\ \Omega$		0.15	0.2	V
		V_{OH} : $R_L = 32\ \Omega$	3.03	3.12		
		V_{OL} : $R_L = 16\ \Omega$		0.28	0.36	
		V_{OH} : $R_L = 16\ \Omega$	2.82	2.97		
SNR	Signal-to-noise ratio	A-weighted, $A_V = -1$, $R_L = 32\ \Omega$, THD+N < 0.4%, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		102		dB
Crosstalk	Channel separation	$R_L = 32\ \Omega$, $A_V = -1$ $F = 1\text{ kHz}$ $F = 20\text{ Hz to } 20\text{ kHz}$		-102 -84		dB
C_i	Input capacitance			1		pF
GBP	Gain bandwidth product	$R_L = 32\ \Omega$		1.1		MHz
SR	Slew rate, unity gain inverting	$R_L = 16\ \Omega$		0.6		V/ μs
V_{IO}	Input offset voltage	$V_{icm} = V_{CC}/2$		1	20	mV
t_{wu}	Wake-up time			100		ms

1. All electrical values are guaranteed with correlation measurements at 2.5 V and 5 V.
2. Guaranteed by design and evaluation.

**Table 6. Electrical characteristics at $V_{CC} = +2.5\text{ V}$
with $GND = 0\text{ V}$, $T_{amb} = 25\text{ °C}$ (unless otherwise specified)**

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
I_{CC}	Supply current	No input signal, no load		1.8	2.5	mA
I_{STBY}	Standby current	No input signal, $V_{STBY} = GND$ for TS488, $R_L = 32\ \Omega$		10	1000	nA
		No input signal, $V_{STBY} = V_{CC}$ for TS489, $R_L = 32\ \Omega$		10	1000	
P_{out}	Output power	THD+N = 0.1% max, $F = 1\text{ kHz}$, $R_L = 32\ \Omega$		19		mW
		THD+N = 1% max, $F = 1\text{ kHz}$, $R_L = 32\ \Omega$	18	20		
		THD+N = 0.1% max, $F = 1\text{ kHz}$, $R_L = 16\ \Omega$		31		
		THD+N = 1% max, $F = 1\text{ kHz}$, $R_L = 16\ \Omega$	27	32		
THD+N	Total harmonic distortion + noise	$A_V = -1$, $R_L = 32\ \Omega$, $P_{out} = 10\text{ mW}$, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		0.3		%
		$A_V = -1$, $R_L = 16\ \Omega$, $P_{out} = 16\text{ mW}$, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		0.3		
PSRR	Power supply rejection ratio, inputs grounded ⁽¹⁾	$A_V = -1$, $R_L \geq 16\ \Omega$, $C_b = 1\ \mu\text{F}$, $F = 1\text{ kHz}$, $V_{ripple} = 200\text{ mVpp}$		68		dB
		$A_V = -1$, $R_L \geq 16\ \Omega$, $C_b = 1\ \mu\text{F}$, $F = 217\text{ Hz}$, $V_{ripple} = 200\text{ mVpp}$		66		
V_O	Output swing	V_{OL} : $R_L = 32\ \Omega$		0.12	0.16	V
		V_{OH} : $R_L = 32\ \Omega$	2.3	2.36		
		V_{OL} : $R_L = 16\ \Omega$		0.22	0.28	
		V_{OH} : $R_L = 16\ \Omega$	2.15	2.25		
SNR	Signal-to-noise ratio	A-weighted, $A_V = -1$, $R_L = 32\ \Omega$, THD+N < 0.4%, $20\text{ Hz} \leq F \leq 20\text{ kHz}$		100		dB
Crosstalk	Channel separation	$R_L = 32\ \Omega$, $A_V = -1$ $F = 1\text{ kHz}$ $F = 20\text{ Hz to } 20\text{ kHz}$		-102 -84		dB
C_i	Input capacitance			1		pF
GBP	Gain bandwidth product	$R_L = 32\ \Omega$		1.1		MHz
SR	Slew rate, unity gain inverting	$R_L = 16\ \Omega$		0.6		V/ μs
V_{IO}	Input offset voltage	$V_{icm} = V_{CC}/2$		1	20	mV
t_{wu}	Wake-up time			100		ms

1. Guaranteed by design and evaluation.

Table 7. Index of graphics

Description	Figure
Open-loop frequency response	Figure 2 to Figure 11
Power derating curves	Figure 12 to Figure 13
Signal-to-noise ratio vs. power supply voltage	Figure 14 to Figure 19
Power dissipation vs. output power per channel	Figure 20 to Figure 22
Power supply rejection ratio vs. frequency	Figure 23 to Figure 25
Total harmonic distortion plus noise vs. output power	Figure 26 to Figure 43
Total harmonic distortion plus noise vs. frequency	Figure 44 to Figure 52
Output power vs. load resistance	Figure 53 to Figure 55
Output power vs. power supply voltage	Figure 56 , Figure 57
Output voltage swing vs. power supply voltage	Figure 58
Current consumption vs. power supply voltage	Figure 59
Current consumption vs. standby voltage	Figure 60 to Figure 65
Crosstalk vs. frequency	Figure 66 to Figure 77

Figure 2. Open-loop frequency response

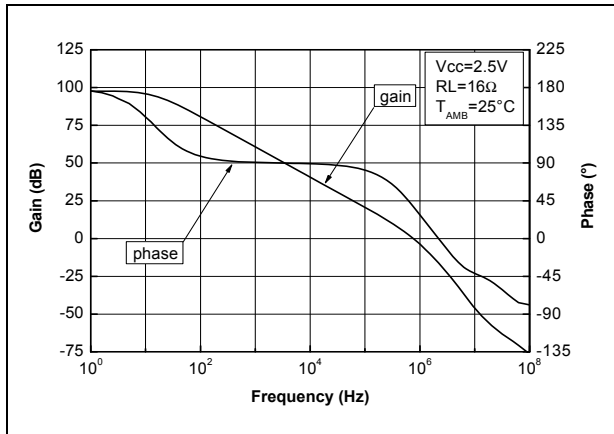


Figure 3. Open-loop frequency response

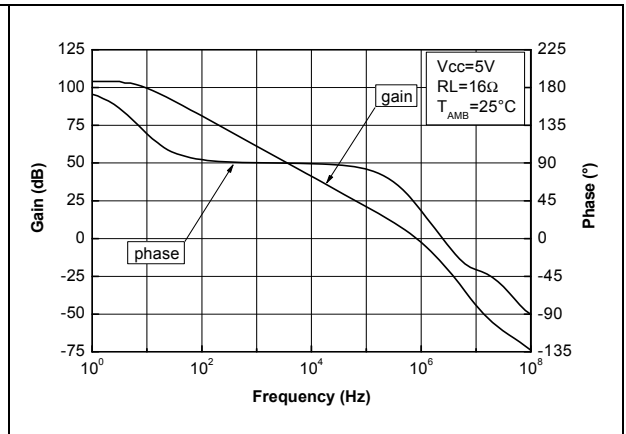


Figure 4. Open-loop frequency response

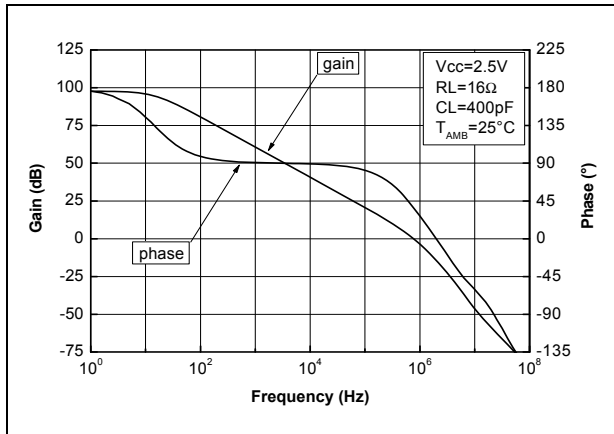


Figure 5. Open-loop frequency response

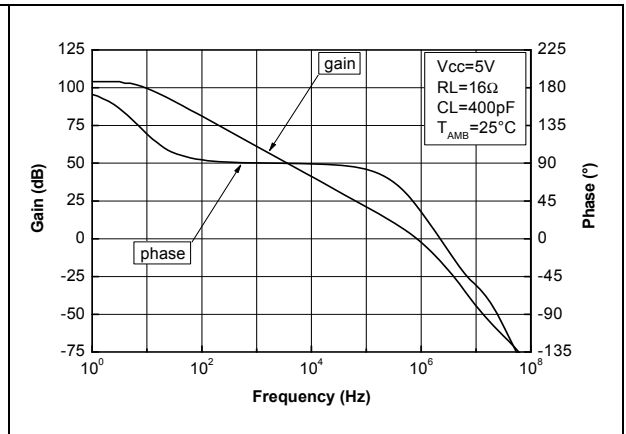


Figure 6. Open-loop frequency response

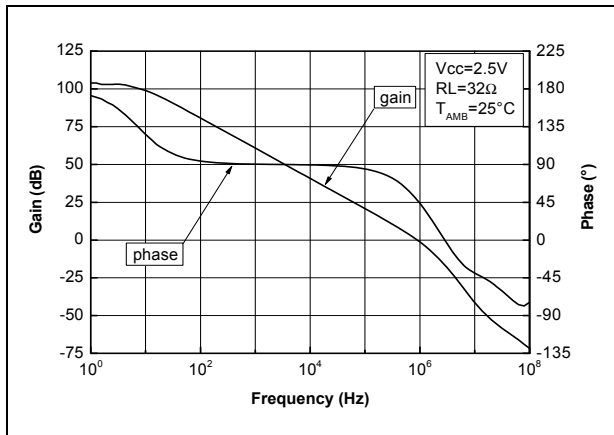


Figure 7. Open-loop frequency response

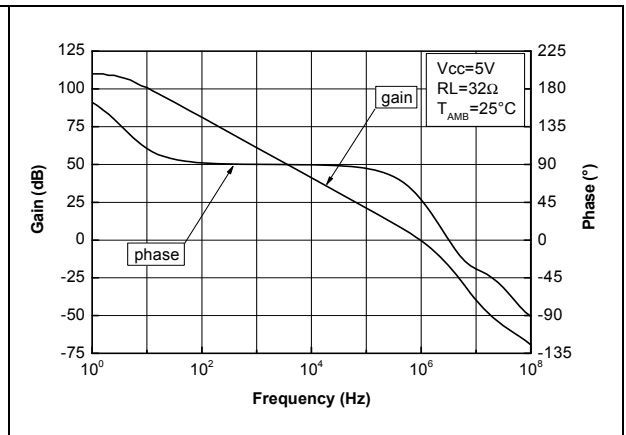


Figure 8. Open-loop frequency response

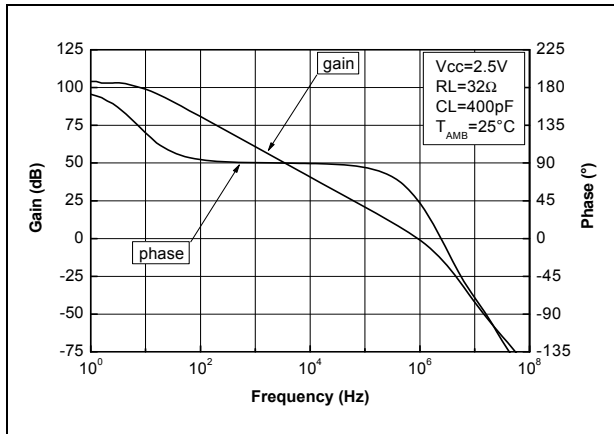


Figure 9. Open-loop frequency response

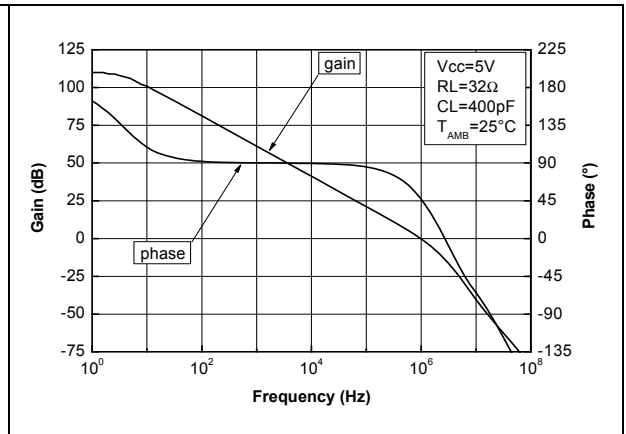


Figure 10. Open-loop frequency response

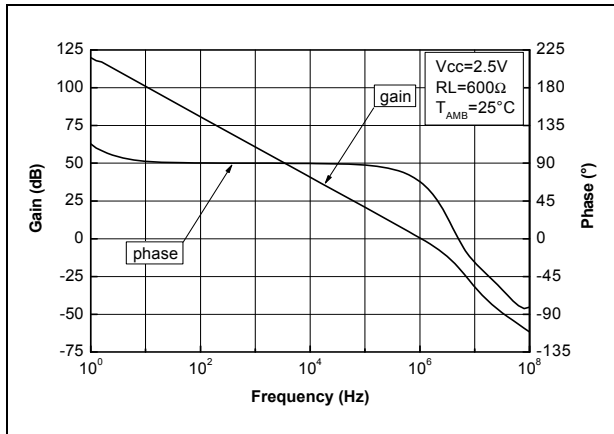


Figure 11. Open-loop frequency response

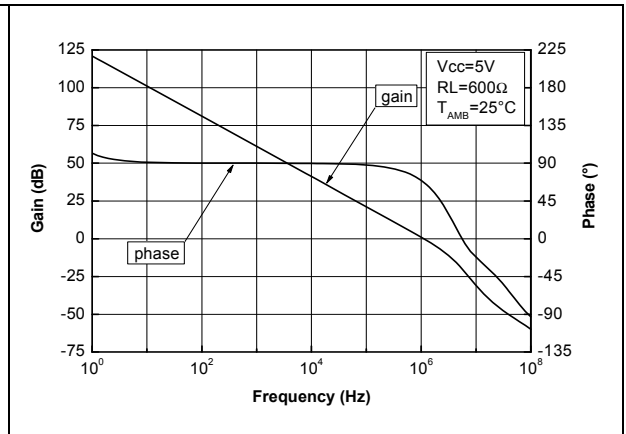


Figure 12. Power derating curves

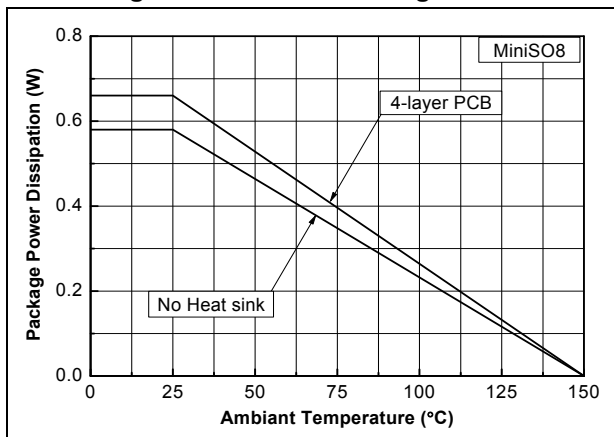


Figure 13. Power derating curves

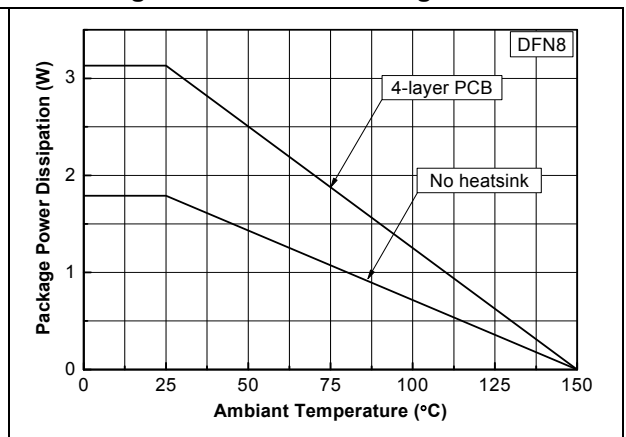


Figure 14. Signal-to-noise ratio vs. power supply voltage

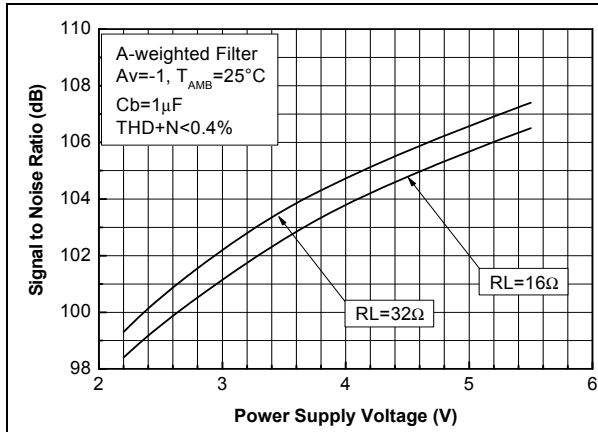


Figure 15. Signal-to-noise ratio vs. power supply voltage

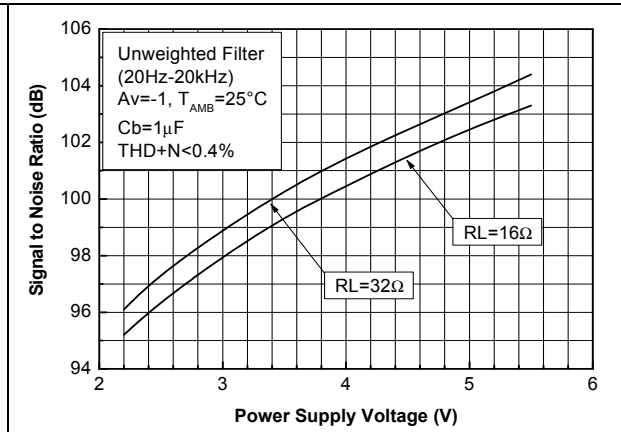


Figure 16. Signal-to-noise ratio vs. power supply voltage

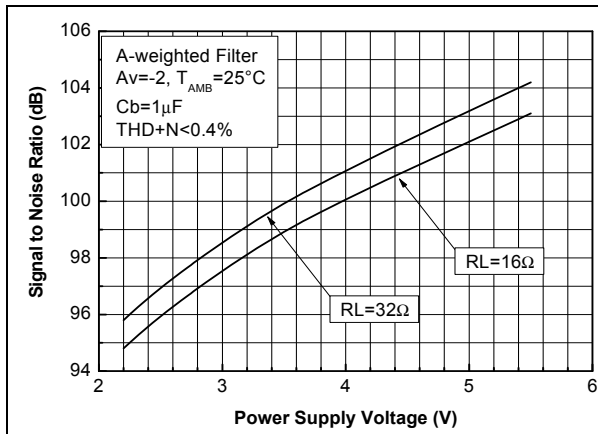


Figure 17. Signal-to-noise ratio vs. power supply voltage

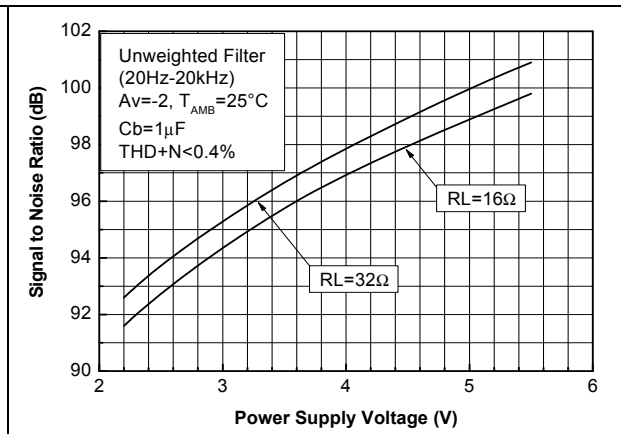


Figure 18. Signal-to-noise ratio vs. power supply voltage

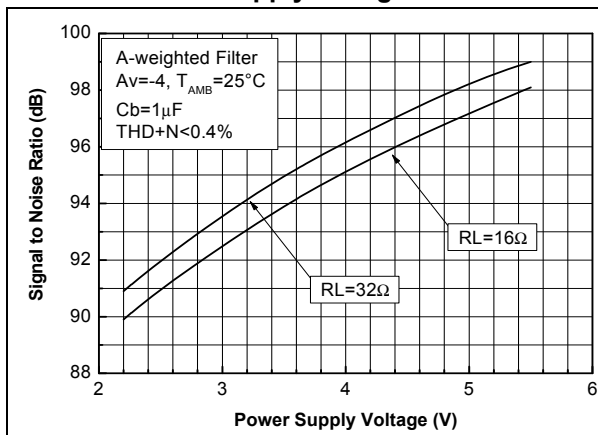


Figure 19. Signal-to-noise ratio vs. power supply voltage

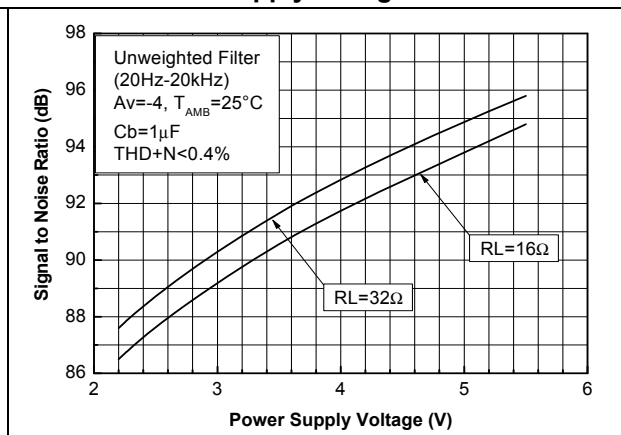


Figure 20. Power dissipation vs. output power per channel

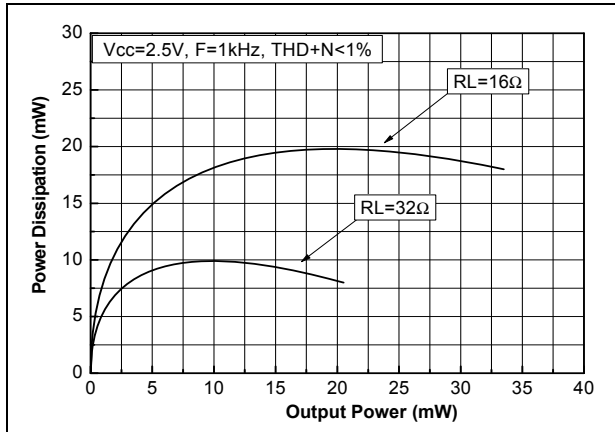


Figure 21. Power dissipation vs. output power per channel

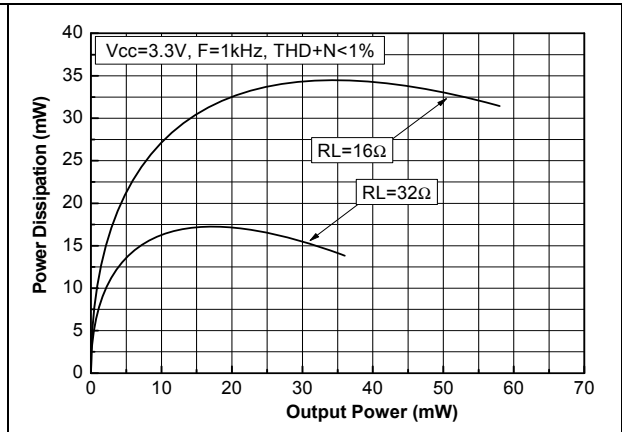


Figure 22. Power dissipation vs. output power per channel

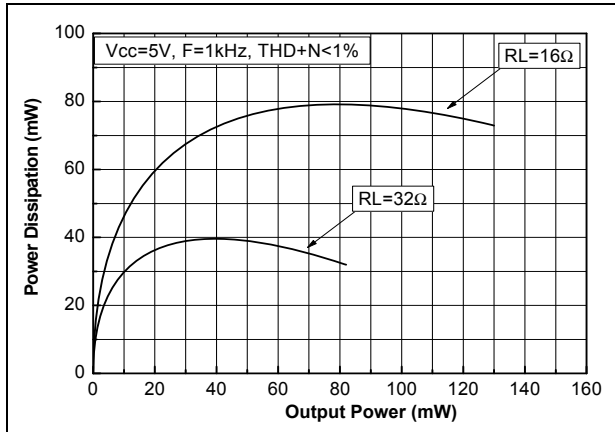


Figure 23. Power supply rejection ratio vs. frequency

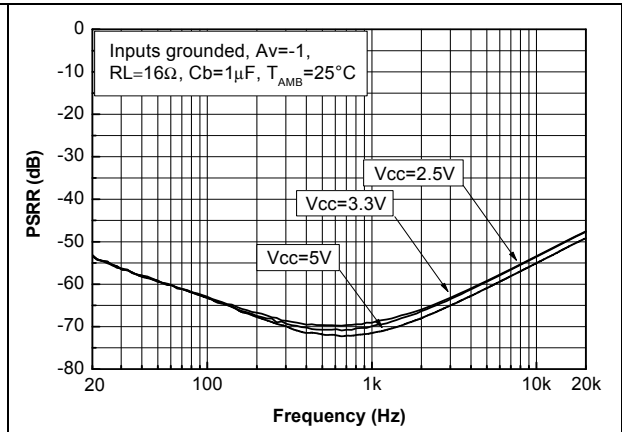


Figure 24. Power supply rejection ratio vs. frequency

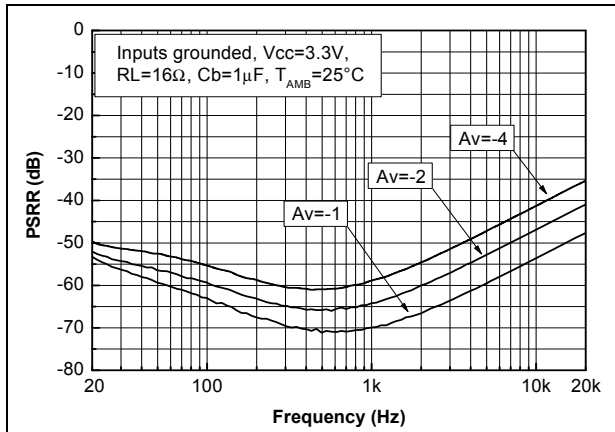


Figure 25. Power supply rejection ratio vs. frequency

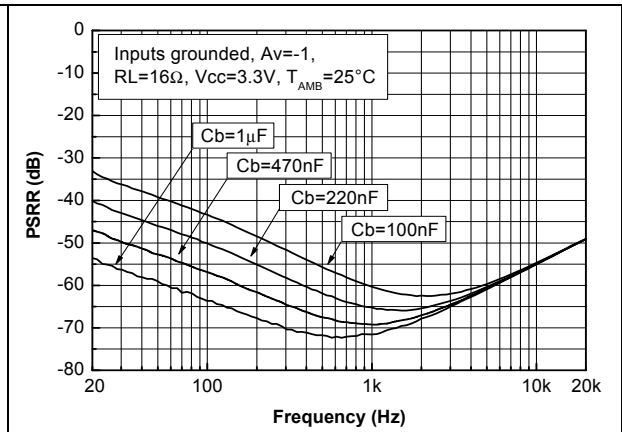


Figure 26. Total harmonic distortion plus noise vs. output power

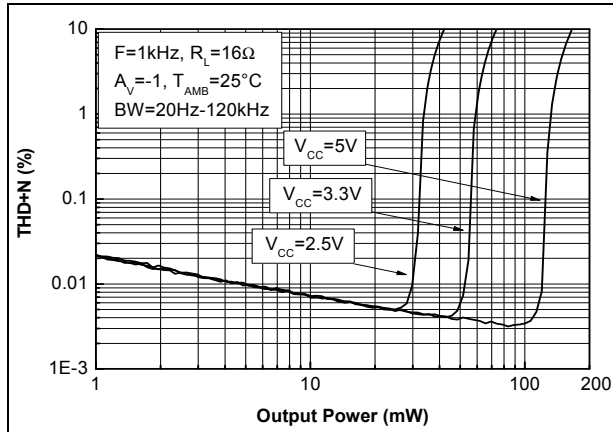


Figure 27. Total harmonic distortion plus noise vs. output power

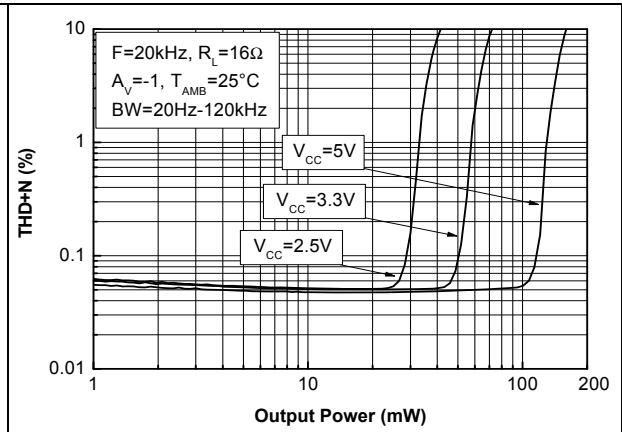


Figure 28. Total harmonic distortion plus noise vs. output power

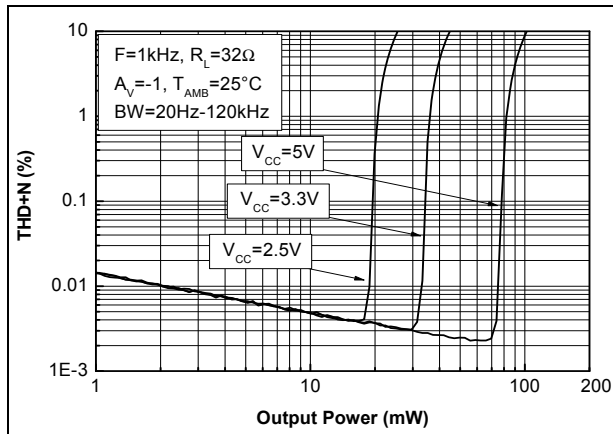


Figure 29. Total harmonic distortion plus noise vs. output power

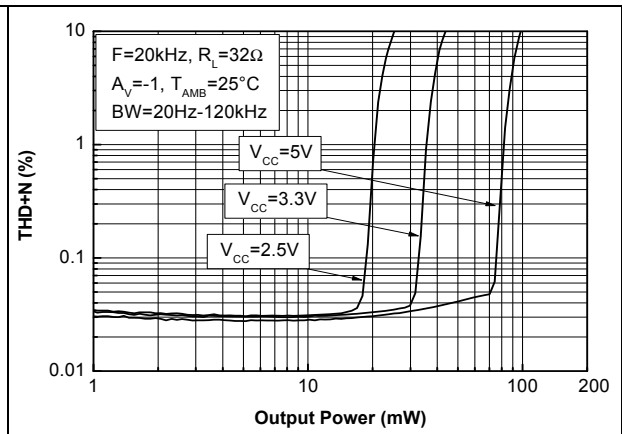


Figure 30. Total harmonic distortion plus noise vs. output power

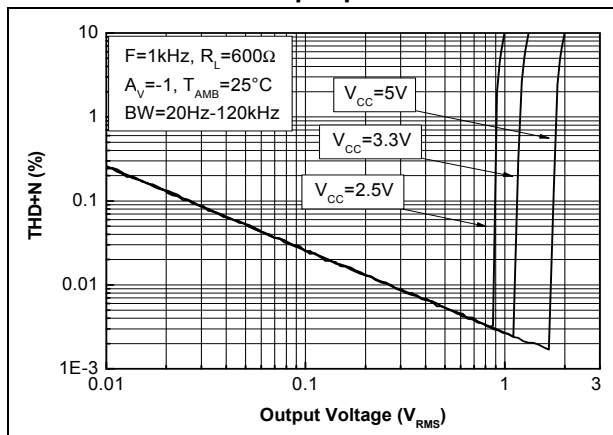


Figure 31. Total harmonic distortion plus noise vs. output power

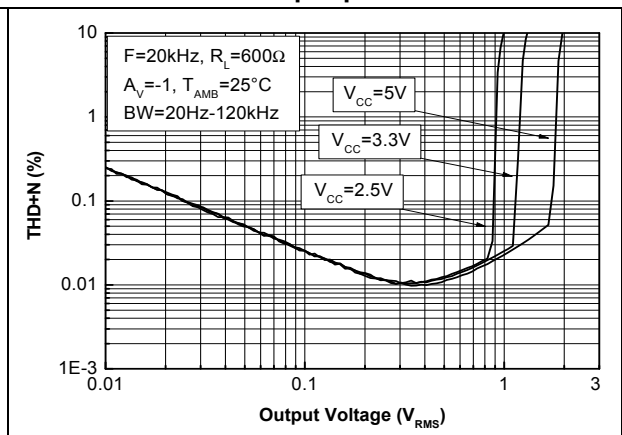


Figure 32. Total harmonic distortion plus noise vs. output power

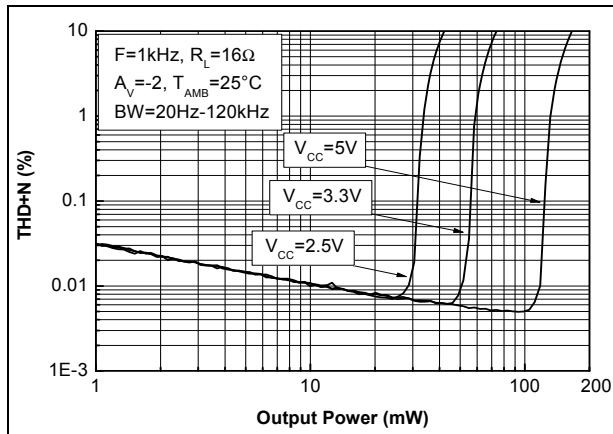


Figure 33. Total harmonic distortion plus noise vs. output power

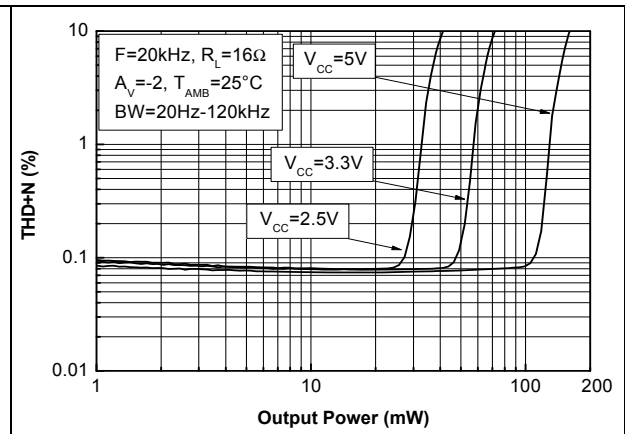


Figure 34. Total harmonic distortion plus noise vs. output power

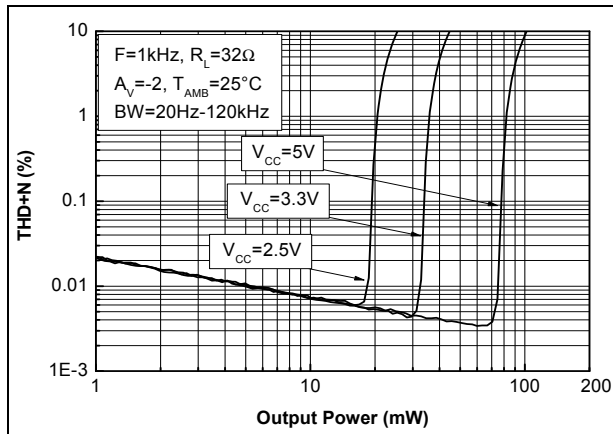


Figure 35. Total harmonic distortion plus noise vs. output power

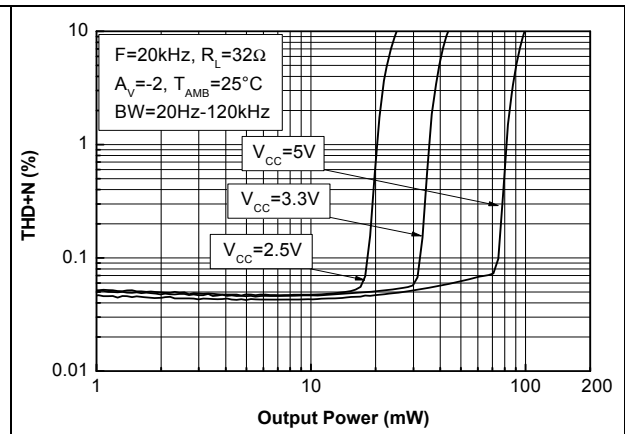


Figure 36. Total harmonic distortion plus noise vs. output power

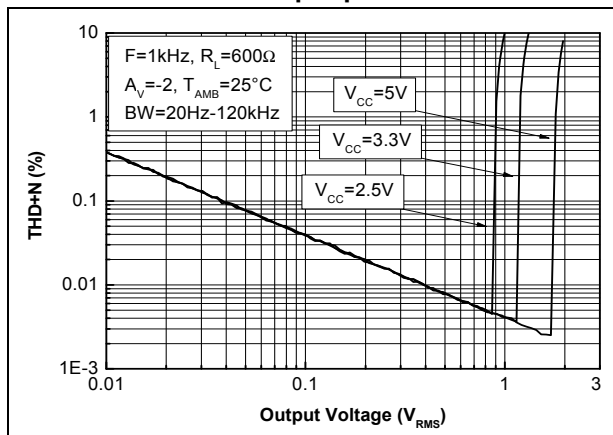


Figure 37. Total harmonic distortion plus noise vs. output power

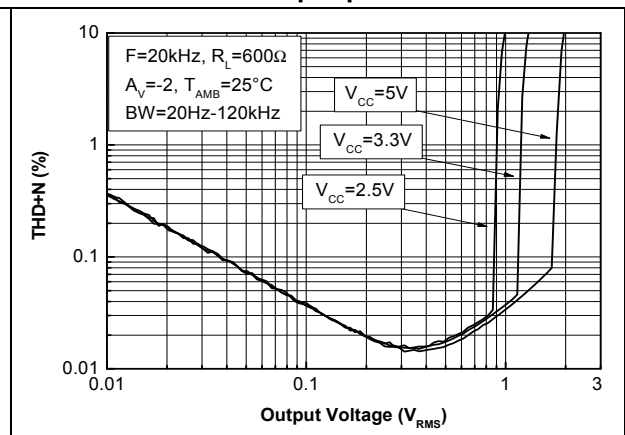


Figure 38. Total harmonic distortion plus noise vs. output power

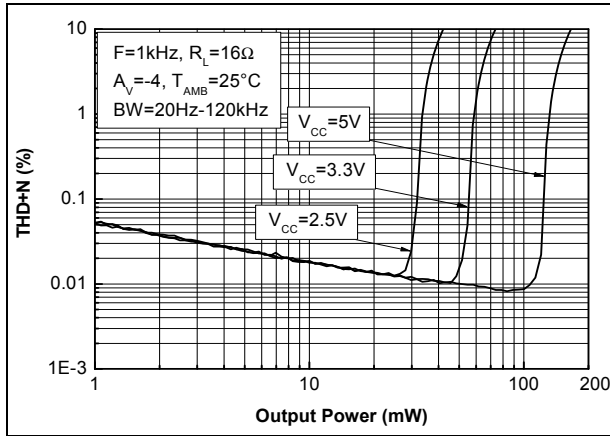


Figure 39. Total harmonic distortion plus noise vs. output power

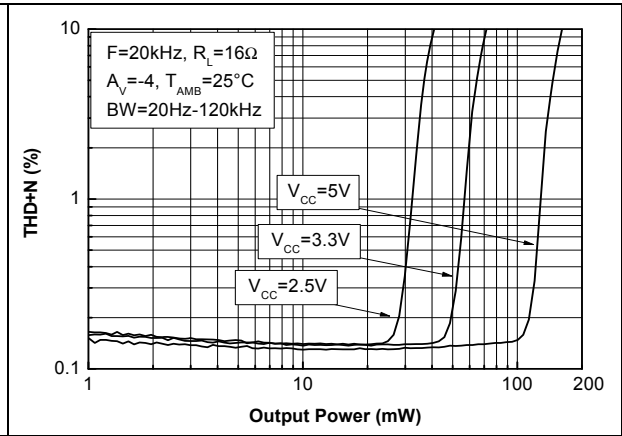


Figure 40. Total harmonic distortion plus noise vs. output power

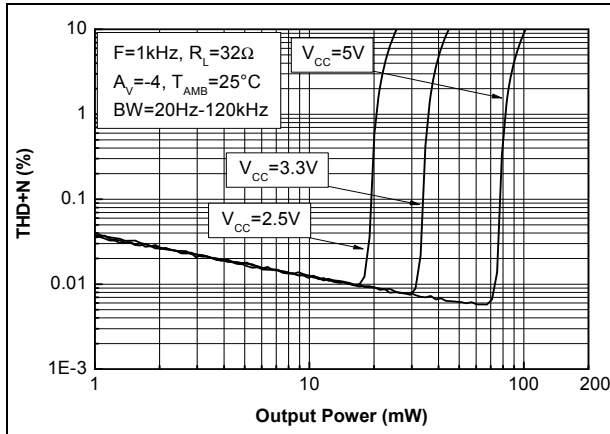


Figure 41. Total harmonic distortion plus noise vs. output power

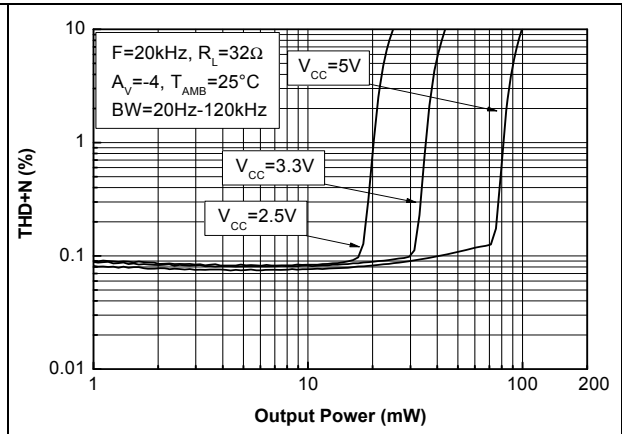


Figure 42. Total harmonic distortion plus noise vs. output power

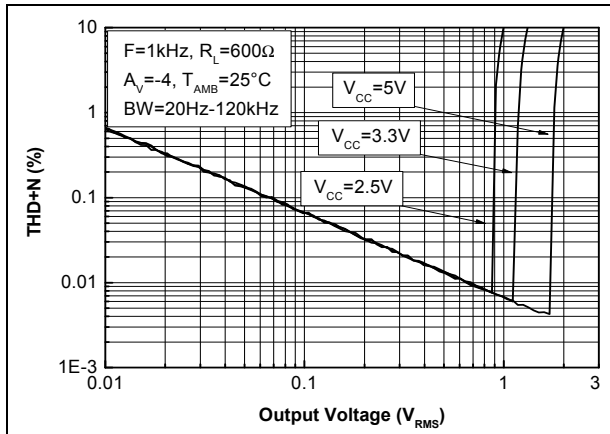


Figure 43. Total harmonic distortion plus noise vs. output power

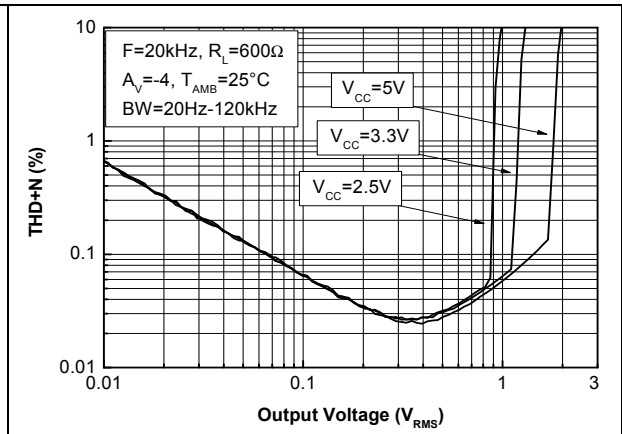


Figure 44. Total harmonic distortion plus noise vs. frequency

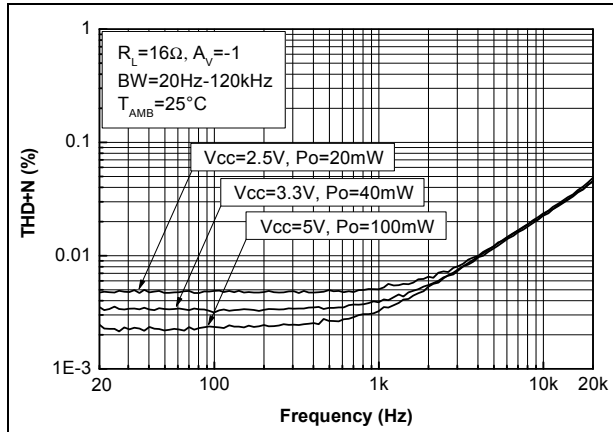


Figure 45. Total harmonic distortion plus noise vs. frequency

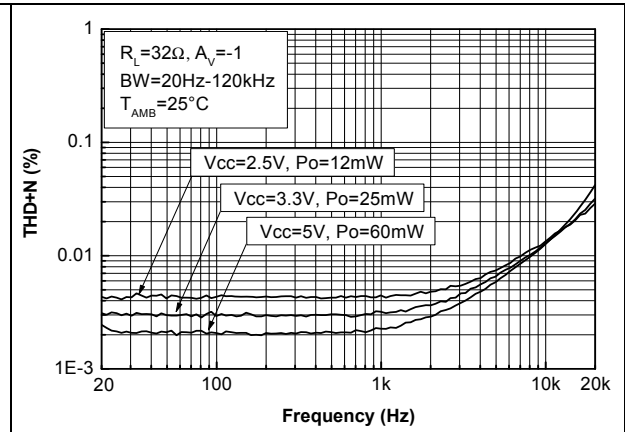


Figure 46. Total harmonic distortion plus noise vs. frequency

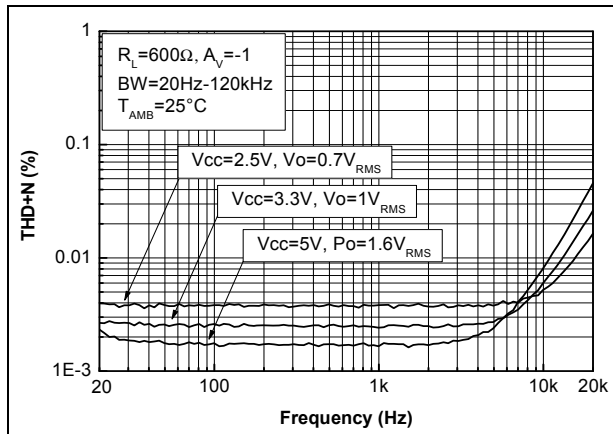


Figure 47. Total harmonic distortion plus noise vs. frequency

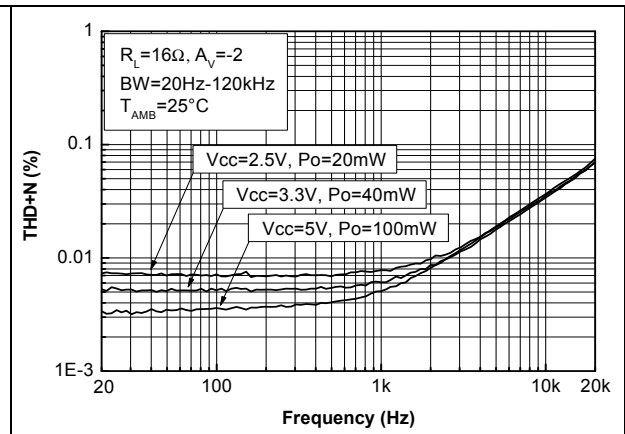


Figure 48. Total harmonic distortion plus noise vs. frequency

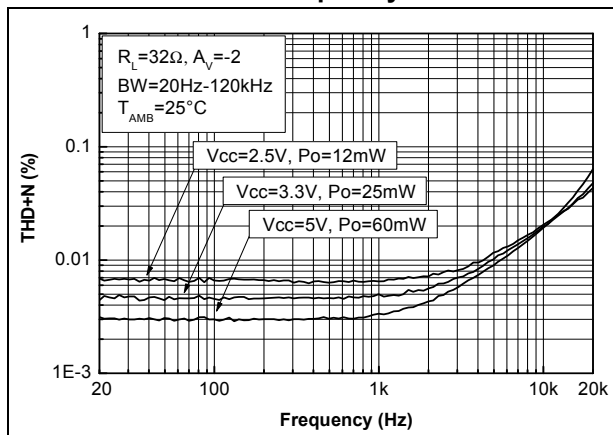


Figure 49. Total harmonic distortion plus noise vs. frequency

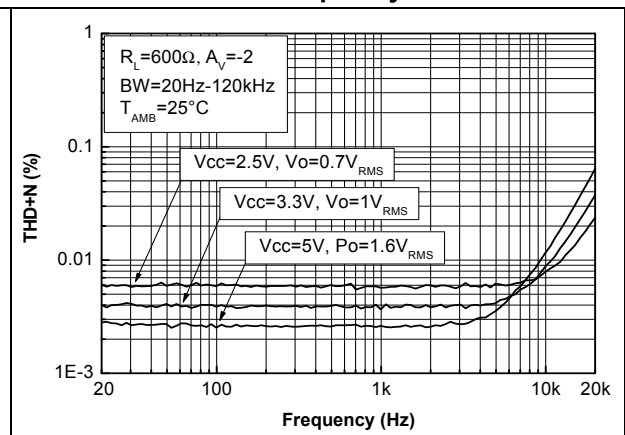


Figure 50. Total harmonic distortion plus noise vs. frequency

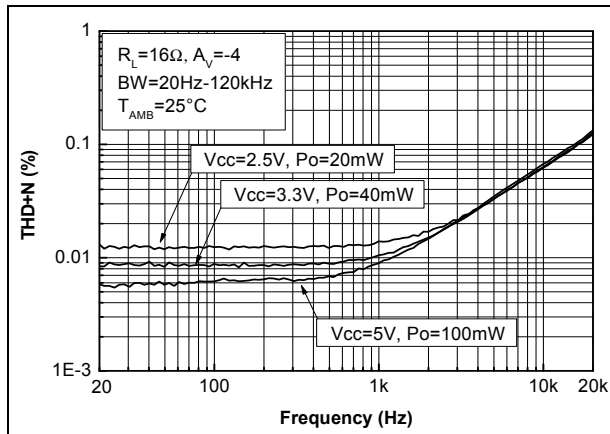


Figure 51. Total harmonic distortion plus noise vs. frequency

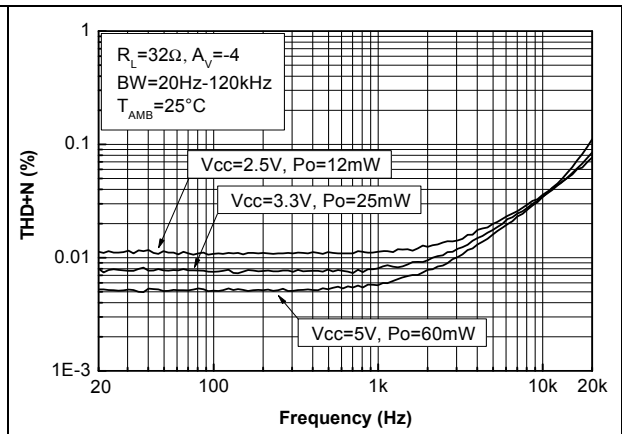


Figure 52. Total harmonic distortion plus noise vs. frequency

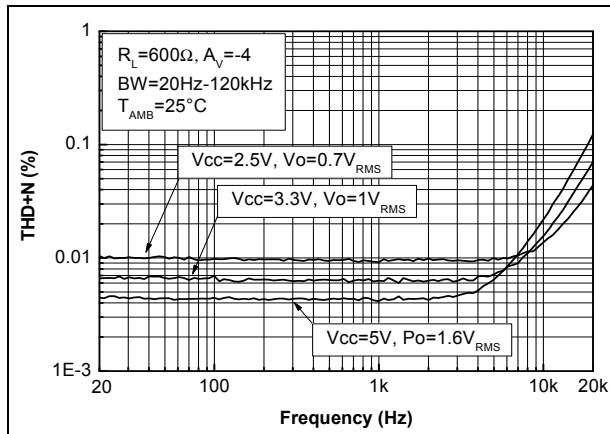


Figure 53. Output power vs. load resistance

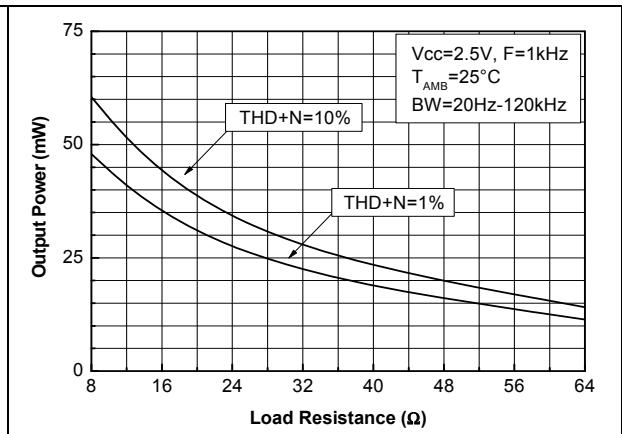


Figure 54. Output power vs. load resistance

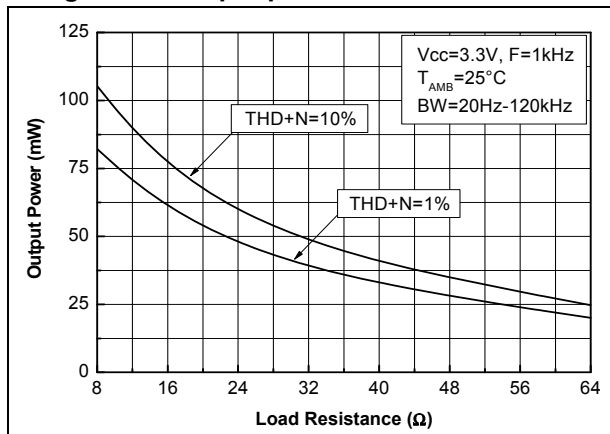


Figure 55. Output power vs. load resistance

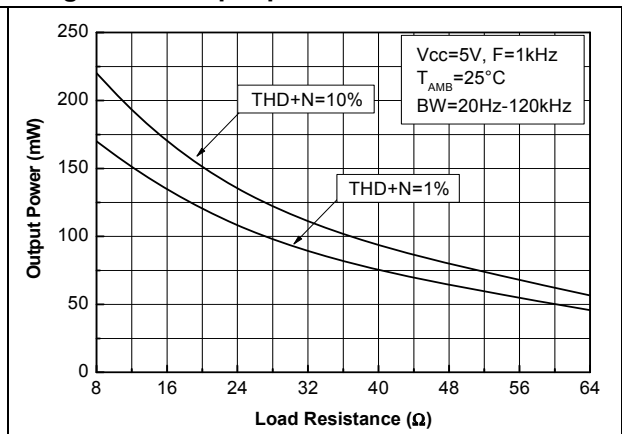


Figure 56. Output power vs. power supply voltage

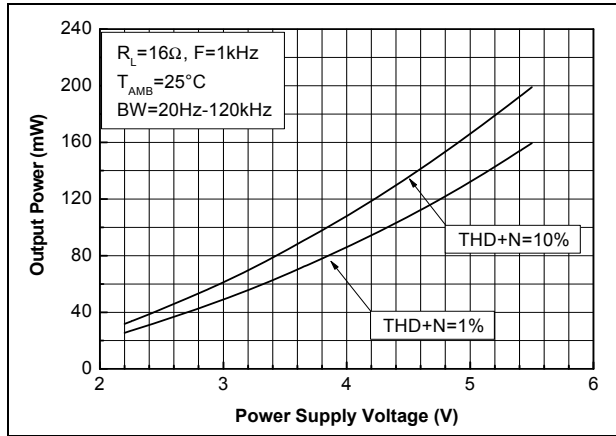


Figure 57. Output power vs. power supply voltage

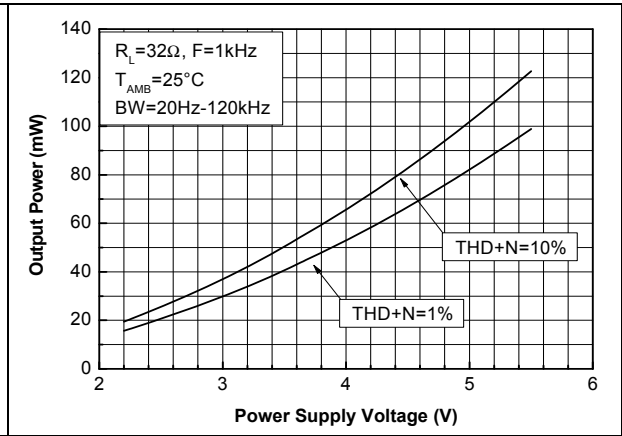


Figure 58. Output voltage swing vs. power supply voltage

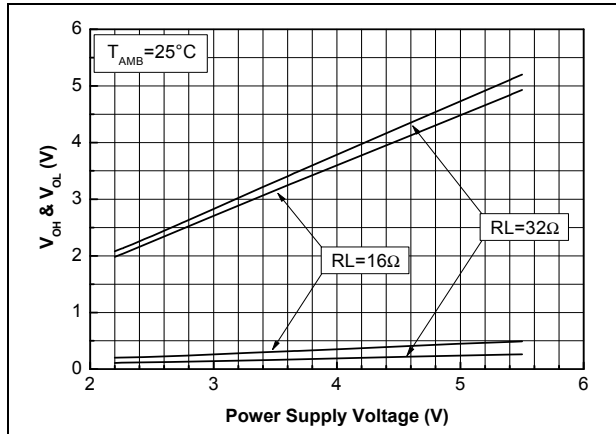


Figure 59. Current consumption vs. power supply voltage

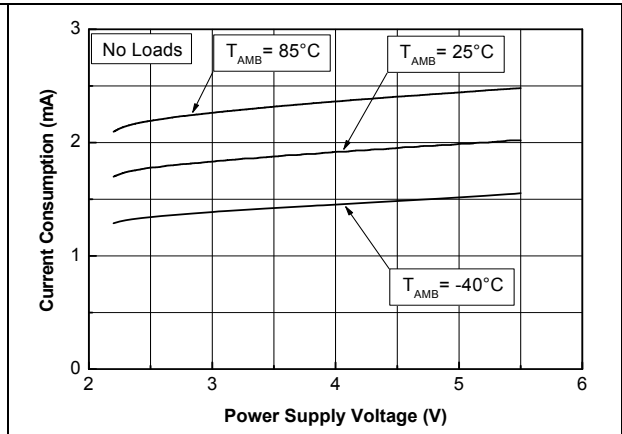


Figure 60. Current consumption vs. standby voltage

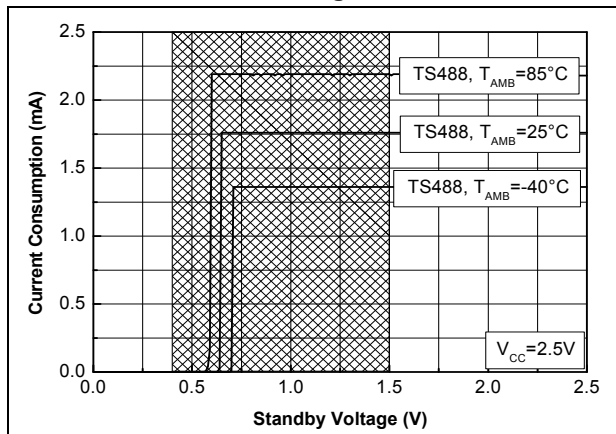


Figure 61. Current consumption vs. standby voltage

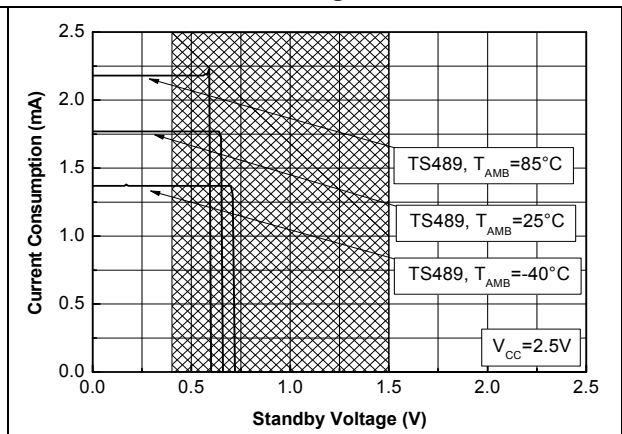


Figure 62. Current consumption vs. standby voltage

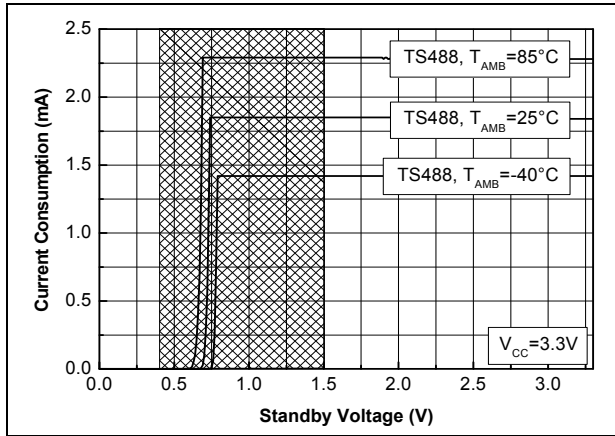


Figure 63. Current consumption vs. standby voltage

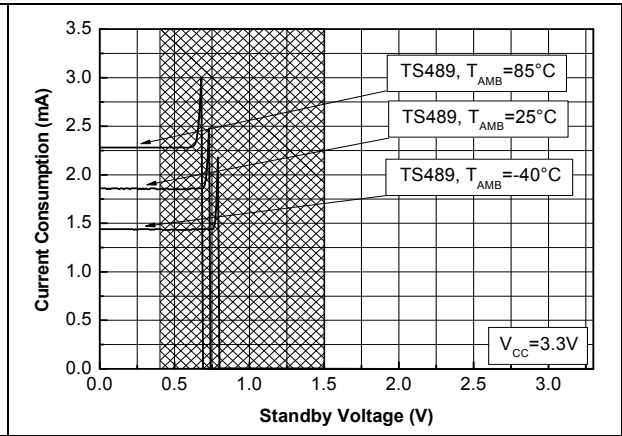


Figure 64. Current consumption vs. standby voltage

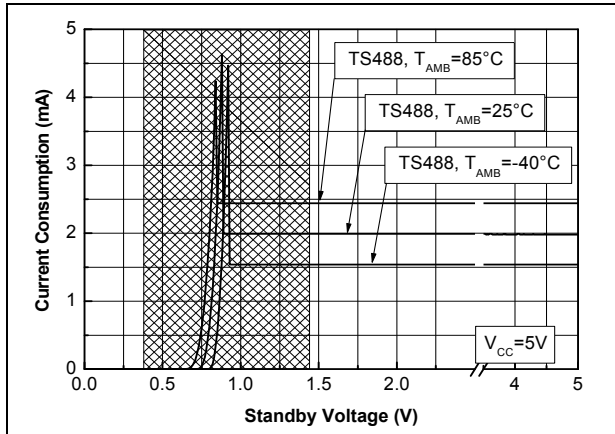


Figure 65. Current consumption vs. standby voltage

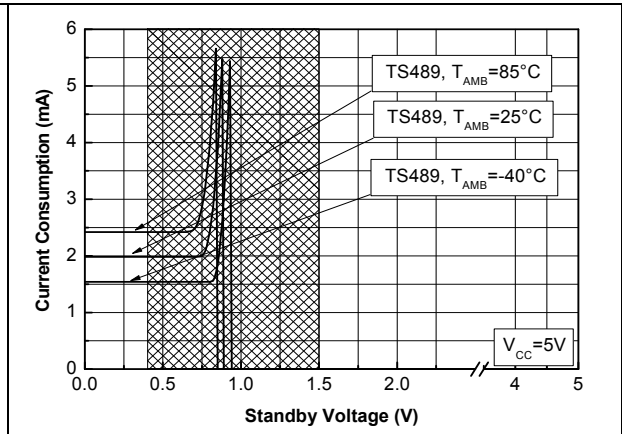


Figure 66. Crosstalk vs. frequency

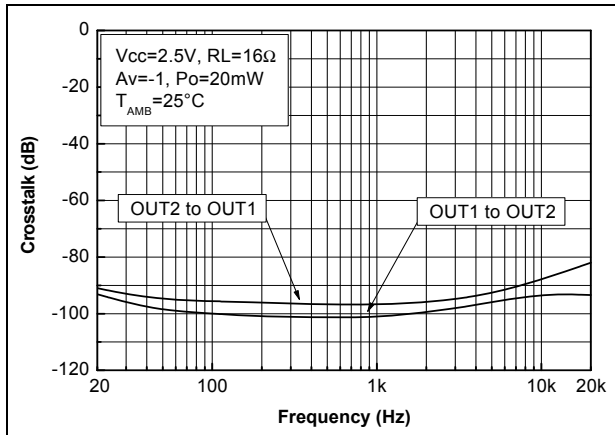


Figure 67. Crosstalk vs. frequency

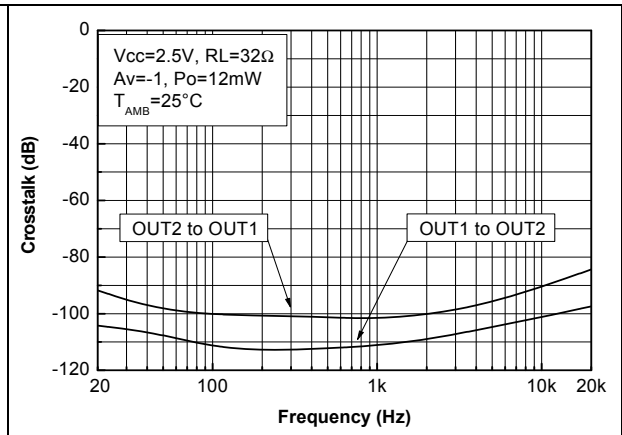


Figure 68. Crosstalk vs. frequency

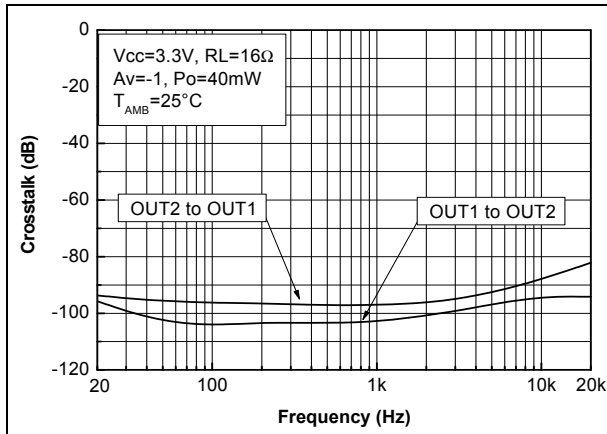


Figure 69. Crosstalk vs. frequency

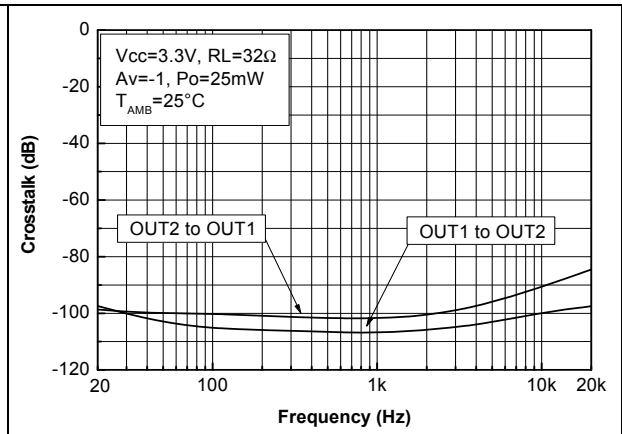


Figure 70. Crosstalk vs. frequency

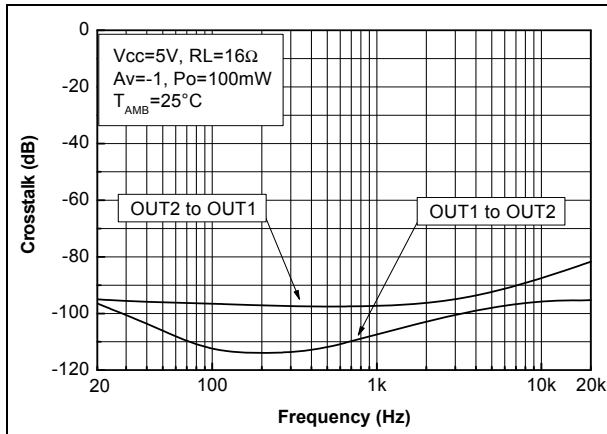


Figure 71. Crosstalk vs. frequency

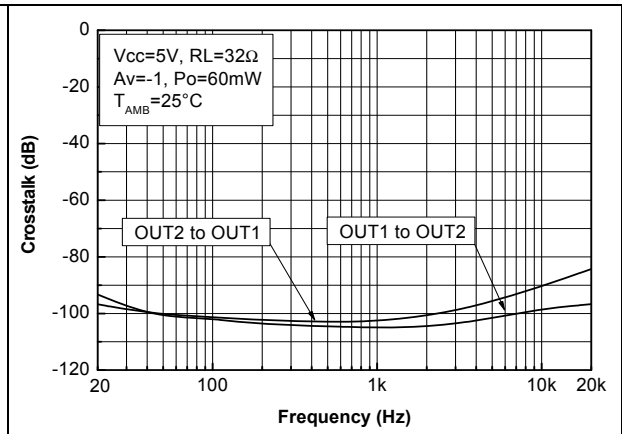


Figure 72. Crosstalk vs. frequency

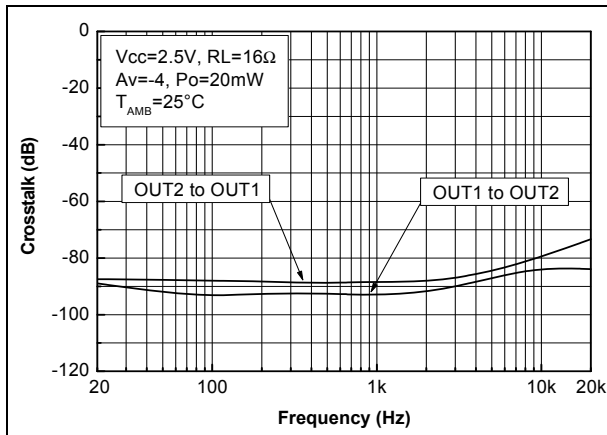


Figure 73. Crosstalk vs. frequency

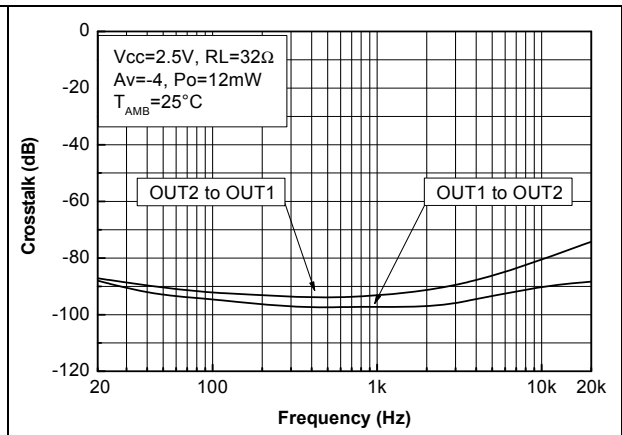


Figure 74. Crosstalk vs. frequency

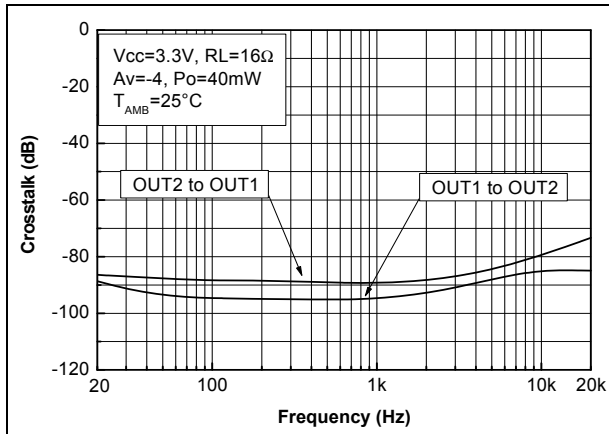


Figure 75. Crosstalk vs. frequency

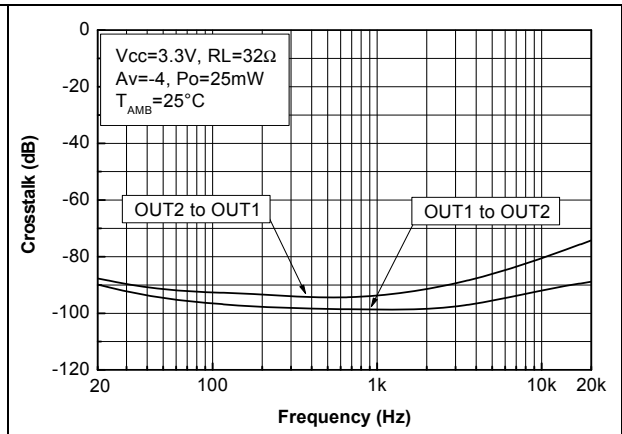


Figure 76. Crosstalk vs. frequency

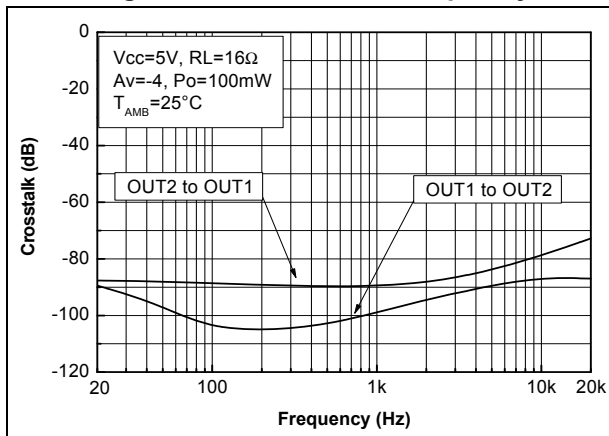
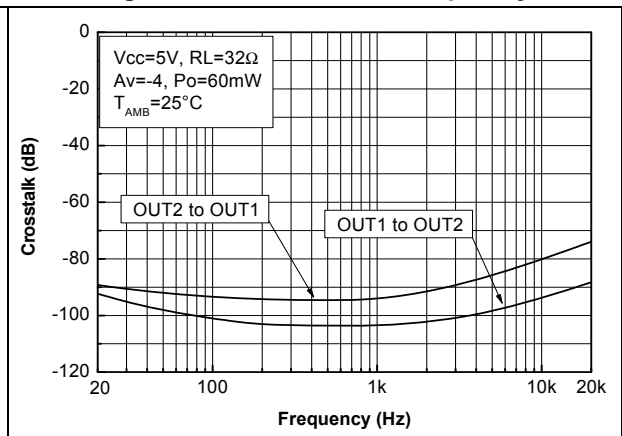


Figure 77. Crosstalk vs. frequency



4 Application information

4.1 Power dissipation and efficiency

Hypotheses:

- Voltage and current in the load are sinusoidal (V_{out} and I_{out}).
- Supply voltage is a pure DC source (V_{CC}).

Regarding the load we have:

$$V_{OUT} = V_{PEAK} \sin \omega t (V)$$

and

$$I_{OUT} = \frac{V_{OUT}}{R_L} (A)$$

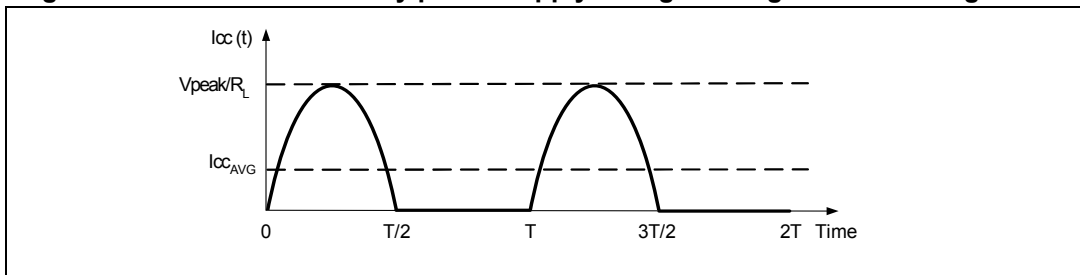
and

$$P_{OUT} = \frac{V_{PEAK}^2}{2R_L} (A)$$

The average current delivered by the power supply voltage is:

$$I_{CC_{AVG}} = \frac{1}{2\pi} \int_0^{\pi} \frac{V_{PEAK}}{R_L} \sin(t) dt = \frac{V_{PEAK}}{\pi R_L} (A)$$

Figure 78. Current delivered by power supply voltage in single-ended configuration



The power delivered by power supply voltage is:

$$P_{supply} = V_{CC} I_{CC_{AVG}} (W)$$

So, the power dissipation by each power amplifier is

$$P_{diss} = P_{supply} - P_{OUT} (W)$$

$$P_{diss} = \frac{\sqrt{2} V_{CC}}{\pi \sqrt{R_L}} \sqrt{P_{OUT}} - P_{OUT} (W)$$

and the maximum value is obtained when:

$$\frac{\partial P_{diss}}{\partial P_{OUT}} = 0$$

and its value is:

$$P_{\text{diss}_{\text{MAX}}} = \frac{V_{\text{CC}}^2}{\pi^2 R_{\text{L}}} \text{ (W)}$$

Note: This maximum value depends only on power supply voltage and load values.

The **efficiency** is the ratio between the output power and the power supply:

$$\eta = \frac{P_{\text{OUT}}}{P_{\text{supply}}} = \frac{\pi V_{\text{peak}}}{2V_{\text{CC}}}$$

The **maximum theoretical value** is reached when $V_{\text{peak}} = V_{\text{CC}}/2$, so

$$\eta = \frac{\pi}{4} = 78.5\%$$

4.2 Total power dissipation

The TS488/9 is stereo (dual channel) amplifier. It has two independent power amplifiers. Each amplifier produces heat due to its power dissipation. Therefore the maximum die temperature is the sum of each amplifier's maximum power dissipation. It is calculated as follows:

- $P_{\text{diss R}}$ = Power dissipation due to the right channel power amplifier.
- $P_{\text{diss L}}$ = Power dissipation due to the left channel power amplifier.
- Total $P_{\text{diss}} = P_{\text{diss R}} + P_{\text{diss L}}$ (W)

Typically, $P_{\text{diss R}}$ is equal to $P_{\text{diss L}}$, giving:

$$\text{Total } P_{\text{diss}} = 2P_{\text{diss R}} = 2P_{\text{diss L}}$$

$$\text{Total } P_{\text{diss}} = \frac{2\sqrt{2}V_{\text{CC}}}{\pi\sqrt{R_{\text{L}}}} \sqrt{P_{\text{OUT}}} - 2P_{\text{OUT}}$$

4.3 Lower cutoff frequency

The lower cutoff frequency F_{CL} of the amplifier depends on input capacitors C_{in} and output capacitors C_{out} .

The input capacitor C_{in} (output capacitor C_{out}) in serial with the input resistor R_{in} (load resistor R_{L}) of the amplifier is equivalent to a first order high pass filter. Assuming that F_{CL} is the lowest frequency to be amplified (with a 3 dB attenuation), the minimum value of the C_{in} (C_{out}) is:

$$C_{\text{in}} = \frac{1}{2\pi \cdot F_{\text{CL}} \cdot R_{\text{in}}}$$

$$C_{\text{out}} = \frac{1}{2\pi \cdot F_{\text{CL}} \cdot R_{\text{L}}}$$

Figure 79. Lower cutoff frequency vs. input capacitor

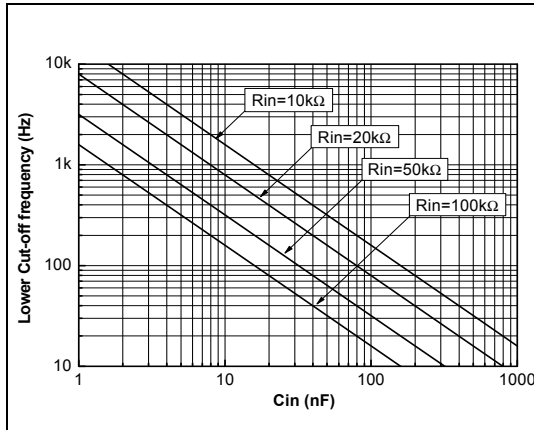
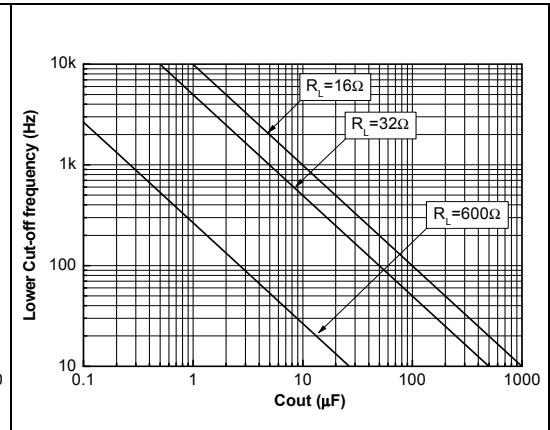


Figure 80. Lower cutoff frequency vs. output capacitor



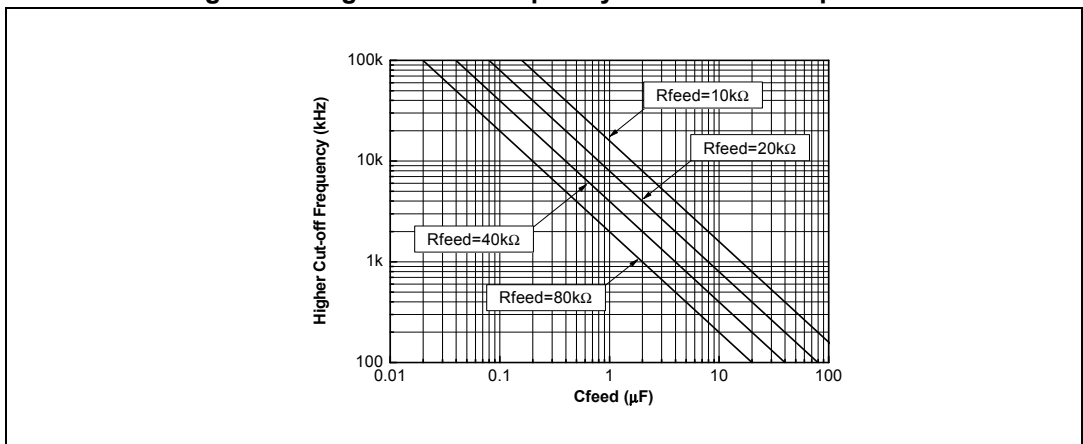
Note: In case F_{CL} is kept the same for calculation, It must be taken in account that the 1st order high-pass filter on the input and the 1st order high-pass filter on the output create a 2nd order high-pass filter in the audio signal path with an attenuation 6 dB on F_{CL} and a roll-off 40db/decade.

4.4 Higher cutoff frequency

In the high-frequency region, you can limit the bandwidth by adding a capacitor C_{feed} in parallel with R_{feed} . It forms a low-pass filter with a -3 dB cutoff frequency F_{CH} . Assuming that F_{CH} is highest frequency to be amplified (with a 3 dB attenuation), the maximum value of C_{feed} is:

$$F_{CH} = \frac{1}{2\pi \cdot R_{feed} \cdot C_{feed}}$$

Figure 81. Higher cutoff frequency vs. feedback capacitor



4.5 Gain setting

In the flat frequency response region (with no effect from C_{in} , C_{out} , C_{feed}), the output voltage is:

$$V_{OUT} = V_{IN} \cdot \left(-\frac{R_{feed}}{R_{in}} \right) = V_{IN} \cdot A_V$$

The gain A_V is:

$$A_V = -\frac{R_{feed}}{R_{in}}$$

4.6 Decoupling of the circuit

Two capacitors are needed to properly bypass the TS488 (TS489), a power supply capacitor C_s and a bias voltage bypass capacitor C_b .

C_s has a strong influence on the THD+N in the high frequency range (above 7kHz) and indirectly on the power supply disturbances. With 1 μ F, you can expect THD+N performance to be similar to the one shown in the datasheet. If C_s is lower than 1 μ F, the THD+N increases in the higher frequencies and disturbances on the power supply rail are less filtered. On the contrary, if C_s is higher than 1 μ F, the disturbances on the power supply rail are more filtered.

C_b has an influence on the THD+N in the low frequency range. Its value is critical on the PSRR with grounded inputs in the lower frequencies:

- If C_b is lower than 1 μ F, the THD+N improves and the PSRR worsens.
- If C_b is higher than 1 μ F, the benefit on the THD+N and PSRR is small.

Note: The input capacitor C_{in} also has a significant effect on the PSRR at lower frequencies. The lower the value of C_{in} , the higher the PSRR.

4.7 Standby mode

When the standby mode is activated an internal circuit of the TS488 (TS489) is charged (see [Figure 82](#)). A time required to change the internal circuit is a few microseconds.

Figure 82. Internal equivalent schematic of the TS488 (TS489) in standby mode

