Application Note

AN- EVAL-2QR4780Z-12W

12W5V Evaluation Board with Quasi-Resonant CoolSET® ICE2QR4780Z

Power Management & Supply

N e v e r s t o p t h i n k i n g .

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Title

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12W5V Evaluation Board with Quasi-Resonant CooLSET® ICE2QR4780Z
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Wong Siew Teng Winson
Winson.wong@infineon.com

Eric Kok
Eric.kok@infineon.com

Jeoh Meng kiat
Mengkiat.jeoh@infineon.com

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1 Content

This application note is a description of 12W switching mode power supply evaluation board designed in a quasi resonant flyback converter topology using ICE2QR4780Z Quasi-resonant CoolSET®.The target application of ICE2QR4780Z are for set-top box, portable game controller, DVD player, netbook adapter and auxiliary power supply for LCD TV, etc. With the CoolMOS® integrated in this IC, it greatly simplifies the design and layout of the PCB. Due to valley switching, the turn on voltage is reduced and this offers higher conversion efficiency comparing to hard-switching flyback converter. With the DCM mode control, the reverse recovery problem of secondary rectify diode is relieved. And for its natural frequency jittering with line voltage, the EMI performance is better. Infineon's digital frequency reduction technology enables a quasi-resonant operation till very low load. As a result, the system efficiency, over the entire load range, is significantly improved compared to conventional free running quasi resonant converter implemented with only maximum switching frequency limitation at light load. In addition, numerous adjustable protection functions have been implemented in ICE2QR4780Z to protect the system and customize the IC for the chosen application. In case of failure modes, like open control-loop/over load, output overvoltage, and transformer short winding, the device switches into **Auto Restart Mode** or **Latch-off Mode**. By means of the cycle-by-cycle peak current limitation plus foldback point correction, the dimension of the transformer and current rating of the secondary diode can both be optimized.Thus, a cost effective solution can be easily achieved.

2 Evaluation Board

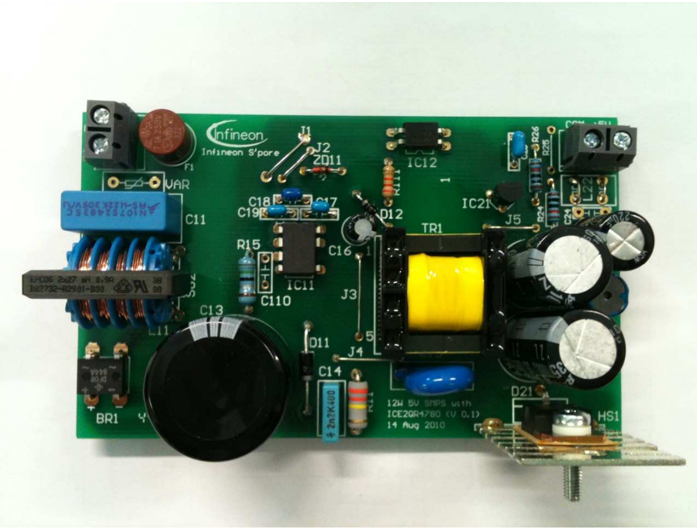


Figure 1-EVALQR-12W-ICE2QR4780Z

3 List of Features

800V avalanche rugged CoolMOS® with built in **depletion startup cell**
Quasi-resonant operation
Digital frequency reduction with decreasing load
Cycle-by-cycle peak current limitation with **foldback point correction**
Built-in **digital soft-start**
Direct current sensing with internal **Leading Edge Blanking Time**
VCC under voltage protection: **IC stop operation, recover with softstart**
VCC over voltage protection: **IC stop operation, recover with softstart**
Openloop/Overload protection: **Auto Restart**
Output overvoltage protection: **Latch-off with adjustable threshold**
Short-winding protection: **Latch-off**
Over temperature protection: **Autorestart**

4 Technical Specifications

Input voltage	**85Vac~282Vac**
Input frequency	**50Hz, 60Hz**
Output voltage and current	**5V 2.4A**
Output power	**12W**
Efficiency	**>80% at full load**
Standby power	**<100mW@no load**
Minimum switching frequency at full load, minimum input voltage	**65kHz**

5 Circuit Description

5.1 Mains Input and Rectification

The AC line input side comprises the input fuse F1 as overcurrent protection. The X2 Capacitors C1 and Choke L1 form a main filter to minimize the feedback of RFI into the main supply. After the bridge rectifier BR1, together with a smoothing capacitor C2, provide a voltage of 70VDC to 380 VDC depending on mains input voltage.

5.2 Integrated MOSFET and PWM Control

ICE2QR4780Z is comprised of a power MOSFET and the quasi-resonant controller; this integrated solution greatly simplifies the circuit layout and reduces the cost of PCB manufacturing. The PWM switch-on is determined by the zero-crossing input signal and the value of the up/down counter. The PWM switch-off is determined by the feedback signal V_{FB} and the current sensing signal V_{CS}. ICE2QR4780Z also performs all necessary protection functions in flyback converters. Details about the information mentioned above are illustrated in the product datasheet.

5.3 Output Stage

On the secondary side, 5V output, the power is coupled out via a schottky diode D21. The capacitors C21 provides energy buffering followed by the L-C filters L21 and C22 to reduce the output ripple and prevent interference between SMPS switching frequency and line frequency considerably. Storage capacitor C21 is designed to have an internal resistance (ESR) as small as possible. This is to minimize the output voltage ripple caused by the triangular current.

5.4 Feedback Loop

For feedback, the output is sensed by the voltage divider of Rc1 and Rc3 and compared to TL431 internal reference voltage. Cc1, Cc2 and Rc4 comprise the compensation network. The output voltage of TL431 is converted to the current signal via optocoupler IC2 and two resistors Rc5 and Rc6 for regulation control.

6 Circuit Operation

6.1 Startup Operation

Since there is a built-in startup cell in the ICE2QR4780Z, there is no need for external start up resistor, which can improve standby performance significantly.
When VCC reaches the turn on voltage threshold 18V, the IC begins with a soft start. The soft-start implemented in ICE2QR4780Z is a digital time-based function. The preset soft-start time is 12ms with 4 steps. If not limited by other functions, the peak voltageon CS pin will increase step by step from 0.32V to 1V finally. After IC turns on, the Vcc voltage is supplied by auxiliary windings of the transformer.

6.2 Normal Mode Operation

The secondary output voltage is built up after startup. The secondary regulation control is adopted with TL431 and optocoupler. The compensation network Cc1, Cc2 and Rc4 constitute the external circuitry of the error amplifier of TL431. This circuitry allows the feedback to be precisely controlled with respect to dynamically varying load conditions, therefore providing stable control.

6.3 Primary side peak current control

The MOSFET drain source current is sensed via external resistor R4 and R4A. Since ICE2QR4780Z is a current mode controller, it would have a cycle-by-cycle primary current and feedback voltage control which can make sure the maximum power of the converter is controlled in every switching cycle.

6.4 Digital Frequency Reduction

During normal operation, the switching frequency for ICE2QR4780Z is digitally reduced with decreasing load. At light load, the MOSFET will be turned on not at the first minimum drain-source voltage time, but on the n_{th}. The counter is in range of 1 to 7, which depends on feedback voltage in a time-base. The feedback voltage decreases when the output power requirement decreases, and vice versa. Therefore, the counter is set by monitoring voltage V_{FB}. The counter will be increased with low V_{FB} and decreased with high V_{FB}. The thresholds are preset inside the IC.

6.5 Burst Mode Operation

At light load condition, the SMPS enters into Active Burst Mode. At this stage, the controller is always active but the Vcc must be kept above the switch off threshold. During active burst mode, the efficiency increase significantly and at the same time it supports low ripple on V_{out} and fast response on load jump.

For determination of entering Active Burst Mode operation, three conditions apply:

1. the feedback voltage is lower than the threshold of V_{FBEB}(1.25V). Accordingly, the peak current sense voltage across the shunt resistor is 0.18;
2. the up/down counter is 7;
3. and a certain blanking time (t_{BEB}).

Once all of these conditions are fulfilled, the Active Burst Mode flip-flop is set and the controller enters Active Burst Mode operation. This multi-condition determination for entering Active Burst Mode operation prevents mistriggering of entering Active Burst Mode operation, so that the controller enters Active Burst Mode operation only when the output power is really low during the preset blanking time.

During active burst mode, the maximum current sense voltage is reduced from 1V to 0.34V so as to reduce the conduction loss and the audible noise. At the burst mode, the FB voltage is changing like a sawtooth between 3.0 and 3.6V.

The feedback voltage immediately increases if there is a high load jump. This is observed by one comparator. As the current limit is 34% during Active Burst Mode a certain load is needed so that feedback voltage can exceed VLB (4.5V). After leaving active busrt mode, maximum current can now be provided to stabilize V_O. In addition, the up/down counter will be set to 1 immediately after leaving Active Burst Mode. This is helpful to decrease the output voltage undershoot

7 Protection Features

7.1 Vcc under voltage and over voltage protection

During normal operation, the VCC voltage is continuously monitored. When the Vcc voltage falls below the under voltage lock out level (VCCoff) or the Vcc voltage increases up to VCCovp, the IC will enter into autorestart mode.

7.2 Foldback point protection

For a quasi-resonant flyback converter, the maximum possible output power is increased when a constant current limit value is used for all the mains input voltage range. This is usually not desired as this will increase additional cost on transformer and output diode in case of output over power conditions.
The internal fold back protection is implemented to adjust the V_{CS} voltage limit according to the bus voltage. Here, the input line voltage is sensed using the current flowing out of **ZC** pin, during the MOSFET on-time. As the result, the maximum current limit will be lower at high input voltage and the maximum output power can be well limited versus the input voltage.

7.3 Open loop/over load protection

In case of open control loop, feedback voltage is pulled up with internally block. After a fixed blanking time 30ms, the IC enters into auto restart mode. In case of secondary short-circuit or overload, regulation voltage V_{FB} will also be pulled up, same protection is applied and IC will auto restart.

7.4 Adjustable output overvoltage protection

During off-time of the power switch, the voltage at the zero-crossing pin ZC is monitored for output overvoltage detection. If the voltage is higher than the preset threshold 3.7V for a preset period 100µs, the IC is latched off.

7.5 Short winding protection

The source current of the MOSFET is sensed via two shunt resistors R4 and R4A in parallel. If the voltage at the current sensing pin is higher than the preset threshold V_{CSSW} of 1.68V during the on-time of the power switch, the IC is latched off. This constitutes a short winding protection. To avoid an accidental latch off, a spike blanking time of 190ns is integrated in the output of internal comparator.

7.6 Auto restart for over temperature protection

The IC has a built-in over temperature protection function. When the controller's temperature reaches 140 ℃, the IC will shut down switch and enters into autorestart. This can protect power MOSFET from overheated.

8 Circuit diagram

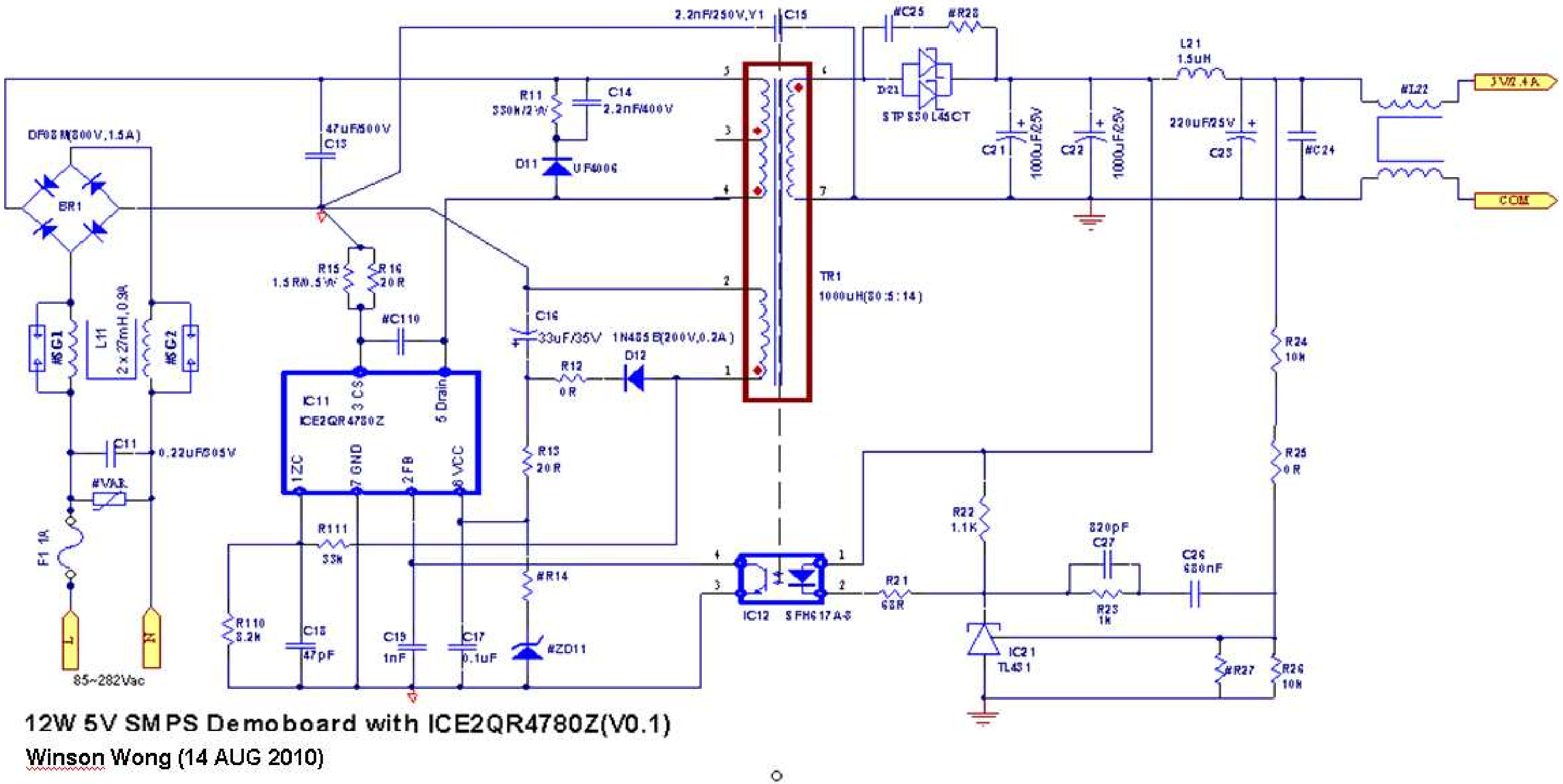


Figure 2 – Schematics

8.1 PCB Top overlayer

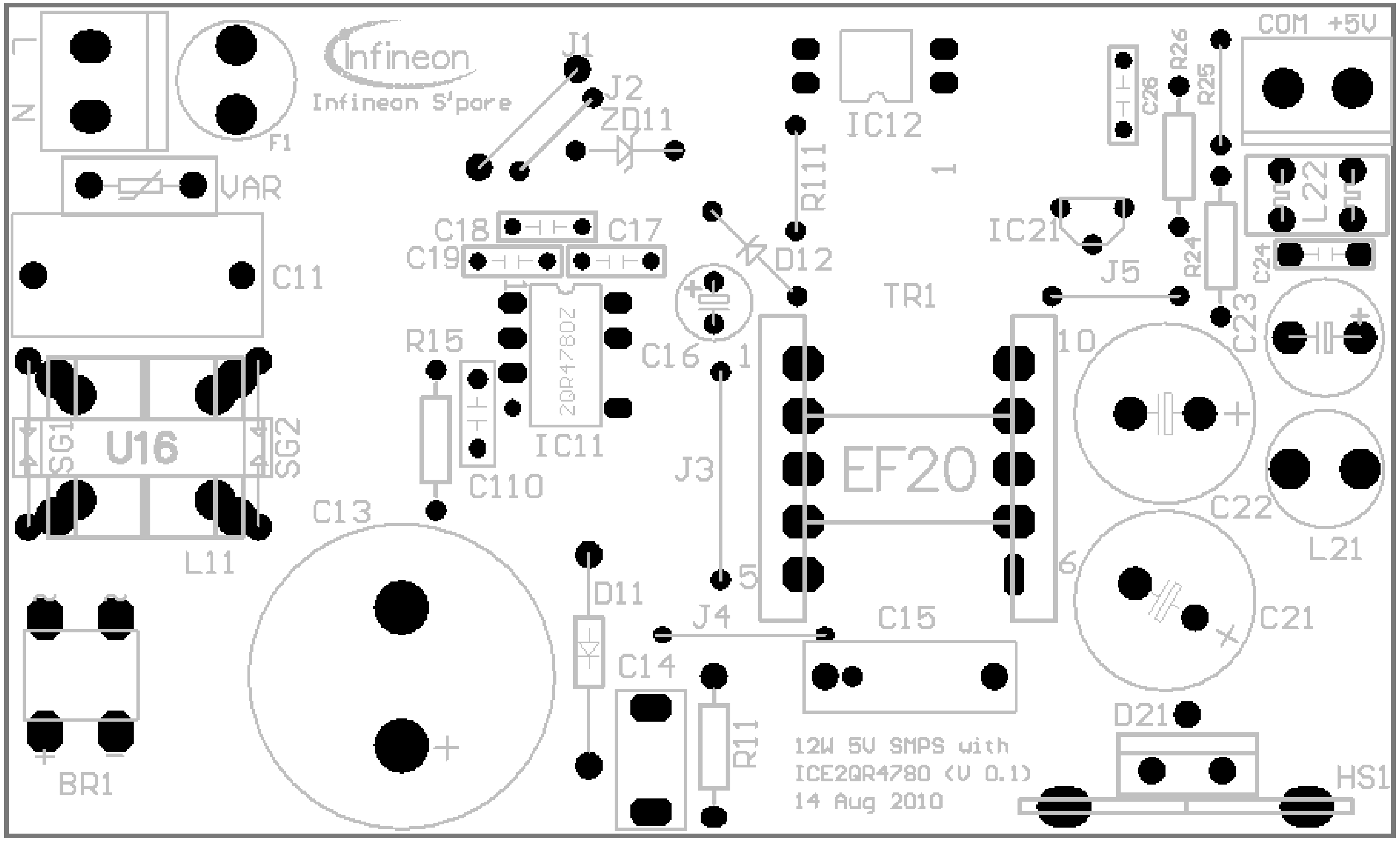


Figure 3 –Component Legend – View from topside

8.2 PCB Bottom Layer

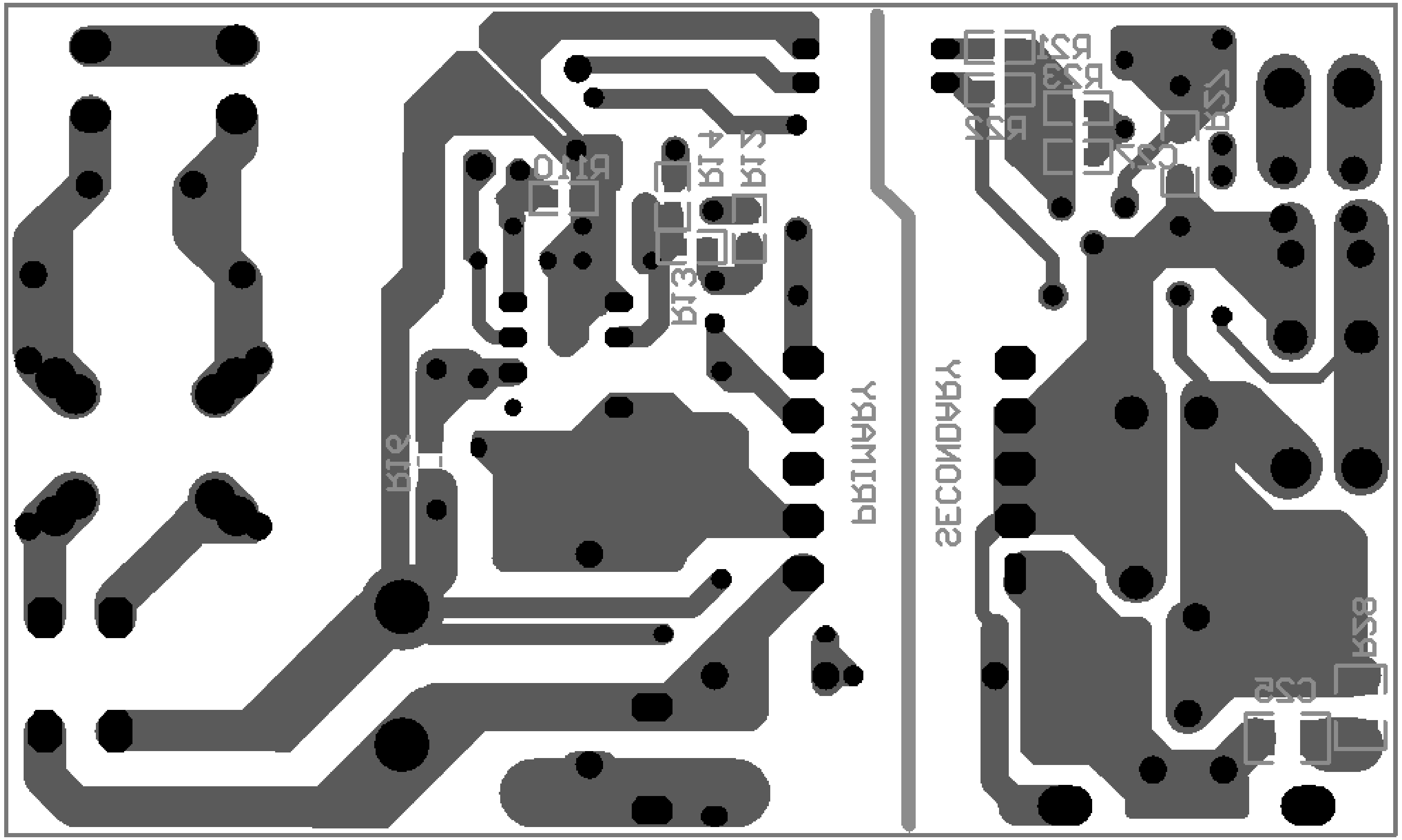


Figure 4 Solder side copper – View from bottom side

9 Component List

Items	Designator	Part Type	Part No.	Manufacturer
1	BR1	Bridge 800V 1.5A	DF08M	
2	F1	1.0A/250Vac		
3	L21	1.5uH		NEC
4	R11	330K, 2W		
5	R13	20R, SMD 0806		
6	R15	1.5R, 0.5W		
7	R16	20R, SMD 0806		
8	R110	8.2k, SMD 0806		
9	R111	33K 0.5W		
10	R21	68R, SMD 0806		
11	R22	1.1k, SMD 0806		
12	R23	1.0k, SMD 0806		
13	R24	10k		
14	R26	10k		
15	C11	0.22uF/305V	B32922X2MKP/2H	Epcos
16	C13	47uF/500V	B43501A6476M000	Epcos
17	C14	2.2nF/400V	MKPS5 2n2M630	
19	C15	2.2nF/250V, Y1	DE1E3KX222MA4BL01	Murata
20	C16	33uF	B41851A7336M	Epcos
21	C17	0.1uF		
22	C18	47pF		
23	C19	1nF		
24	C21	1000uF/35V		KZE
25	C22	1000uF/35V		KZE
26	C23	220uF/25V		KZE
27	C26	680nF		
28	C27	820pF,SMD 0806		
29	L11 EMI	2 x 27mH, 0.9A	B82732R2901B30	Epcos
30	TR1	1000uH (80:5:14)		
31	IC12	SFH617A-3		
32	IC21	TL431		
33	D11	UF4006	UF4006	Vishay
34	D12	1N485B		
35	ZD11	22V zener diode		
36	D21	STPS30L45CT		
37	IC11	ICE2QR4780Z	ICE2QR4780Z	Infineon

Table 1– Component List

10 Transformer Construction

Core and material :EPCOS(N87), E20/10/6
Bobbin: Horizontal Version
Primary Inductance, Lp=1000µH(±3%), measured between pin 4 and pin 5 (Gapped to Inductance)
Air Gap in center leg

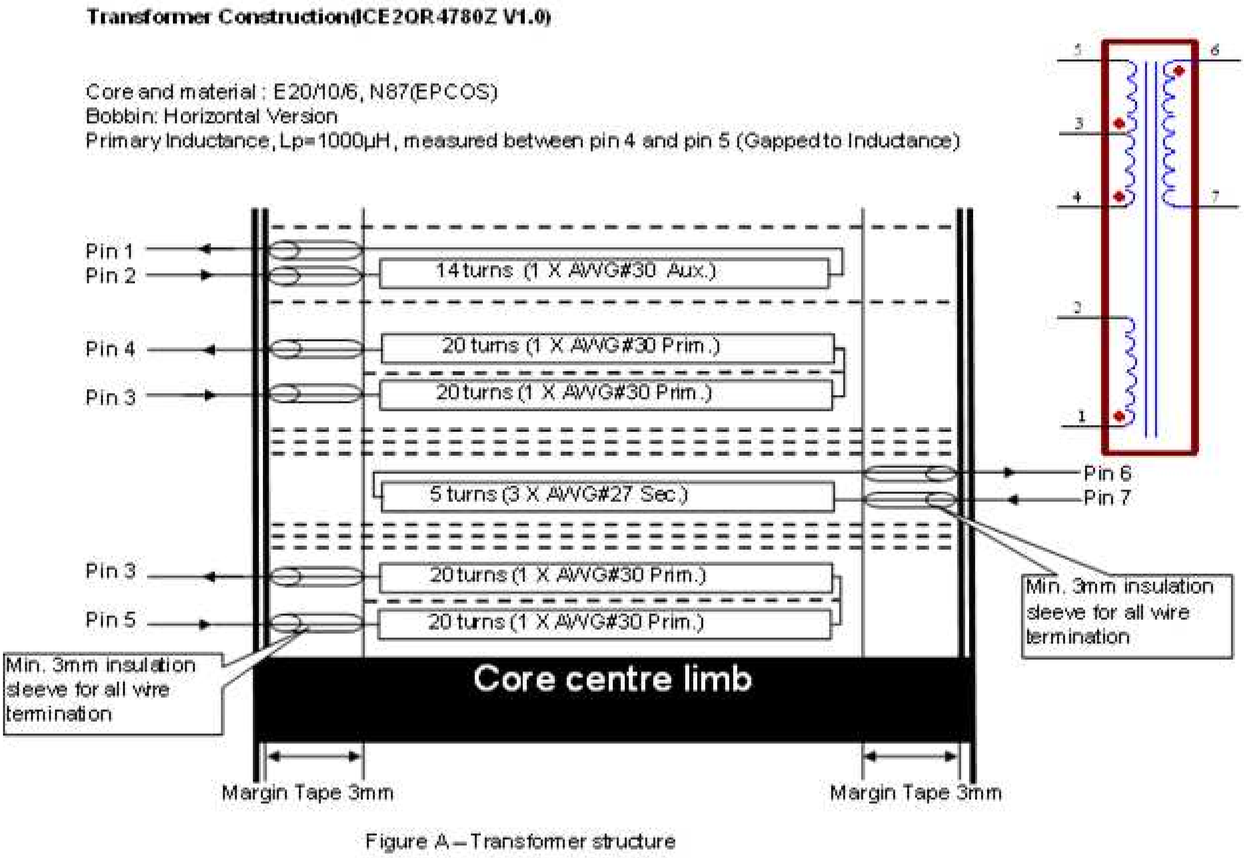


Figure 5 – Transformer structure

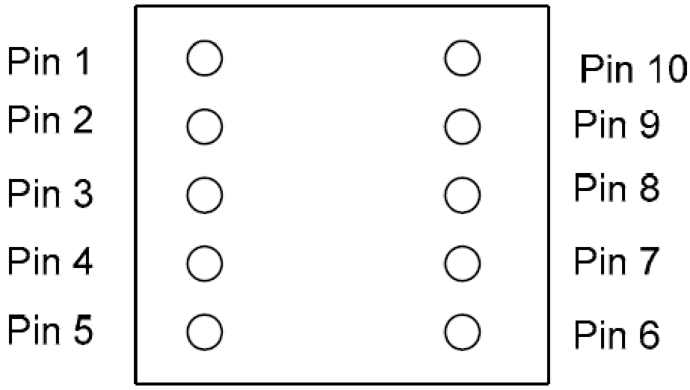


Figure 6 – Transformer complete – top view

Start	Stop	No. of turns	Wire size	Layer
2	1	14	1XAWG#30	Auxiliary
3	4	40	1XAWG#30	$^1/_2$ Primary
7	6	5	3XAWG#27	Secondary
5	3	40	1XAWG#30	$^1/_2$ Primary

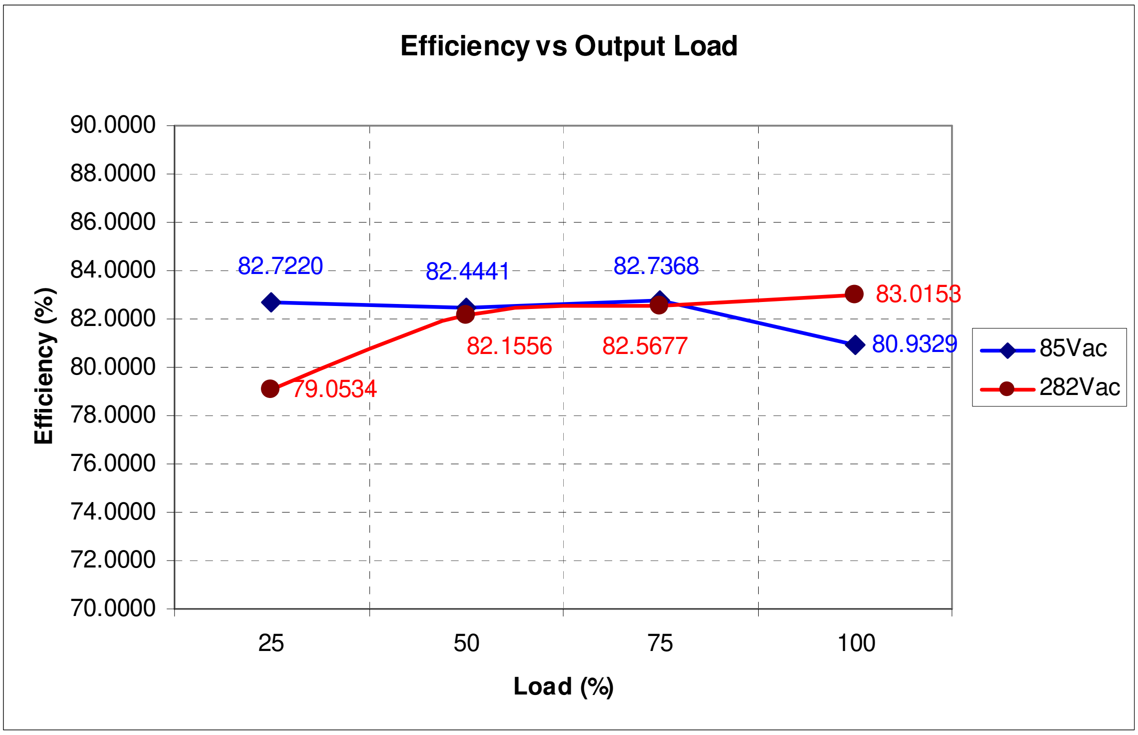
Table 2 wire gauge used of the transformer windings

11 Test Results

11.1 Efficiency and standby performance

Vin (Vac)	Pin (W)	Vo(Vdc)	Io(A)	Po(W)	η(%)	Avg η(%)
85	3.615	4.984	0.6	2.9904	82.7220	82.2090
	7.25	4.981	1.2	5.9772	82.4441	
	10.83	4.978	1.8	8.9604	82.7368	
	14.75	4.974	2.4	11.9376	80.9329	
115	3.586	4.983	0.6	2.9898	83.3742	83.6004
	7.136	4.981	1.2	5.9772	83.7612	
	10.65	4.978	1.8	8.9604	84.1352	
	14.36	4.974	2.4	11.9376	83.1309	
150	3.6	4.983	0.6	2.9898	83.0500	83.7247
	7.146	4.98	1.2	5.976	83.6272	
	10.638	4.977	1.8	8.9586	84.2132	
	14.21	4.974	2.4	11.9376	84.0084	
180	3.62	4.983	0.6	2.9898	82.5912	83.7636
	7.126	4.98	1.2	5.976	83.8619	
	10.62	4.977	1.8	8.9586	84.3559	
	14.17	4.974	2.4	11.9376	84.2456	
230	3.69	4.983	0.6	2.9898	81.0244	82.8945
	7.18	4.98	1.2	5.976	83.2312	
	10.73	4.977	1.8	8.9586	83.4911	
	14.24	4.974	2.4	11.9376	83.8315	
282	3.782	4.983	0.6	2.9898	79.0534	81.6980
	7.274	4.98	1.2	5.976	82.1556	
	10.85	4.977	1.8	8.9586	82.5677	
	14.38	4.974	2.4	11.9376	83.0153	

Table 3 – Efficiency vs. Load



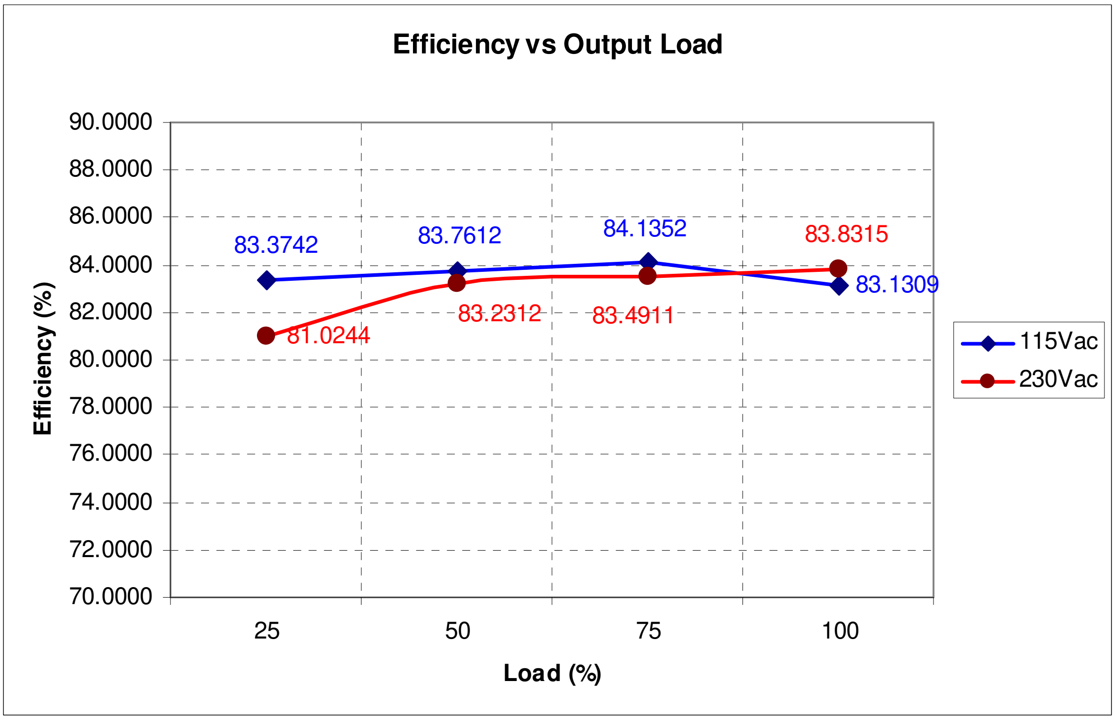


Figure 7a & 7b – Efficiency vs. Output Load

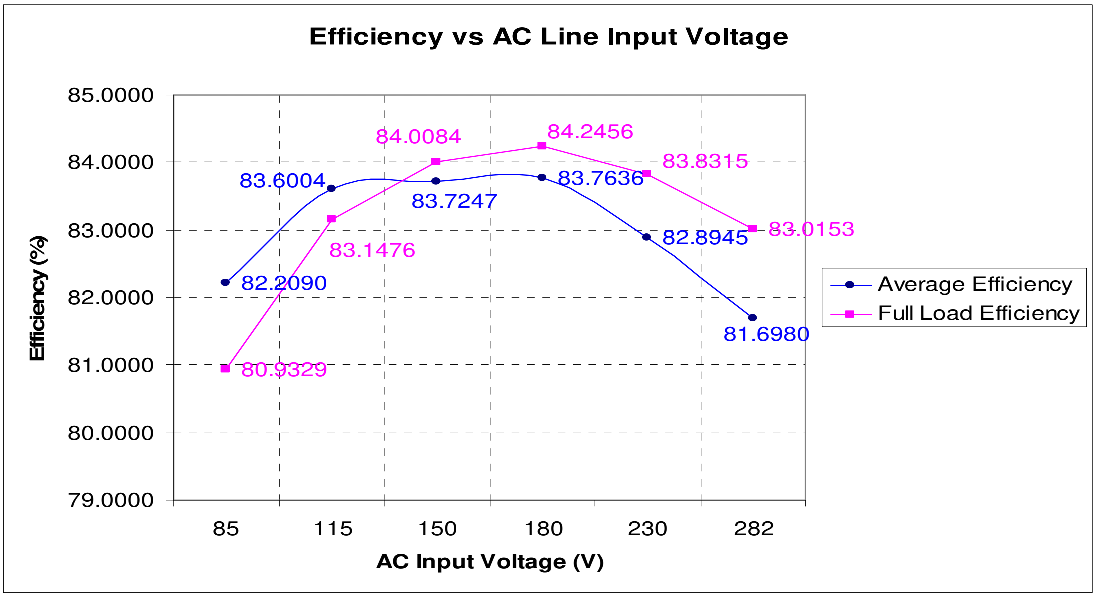


Figure 8 Efficiency vs AC line voltage

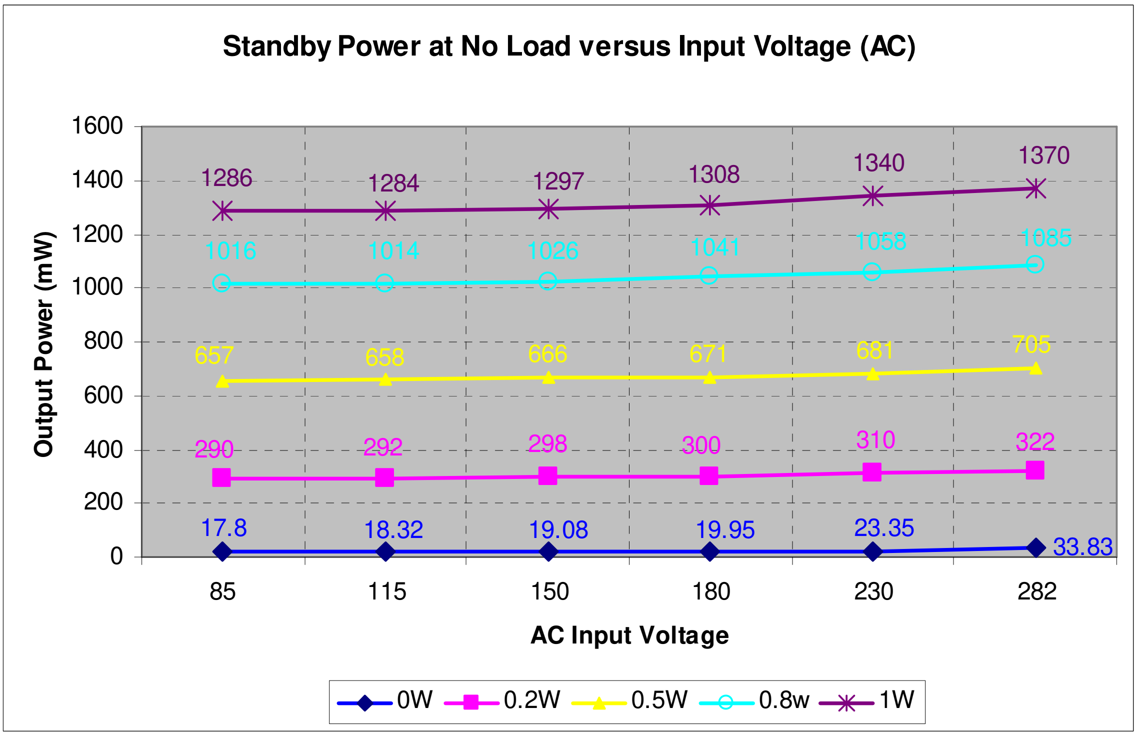


Figure 9 Standby input power vs AC line voltage

12 Waveforms and Scope Plots

12.1 Startup at Full Load

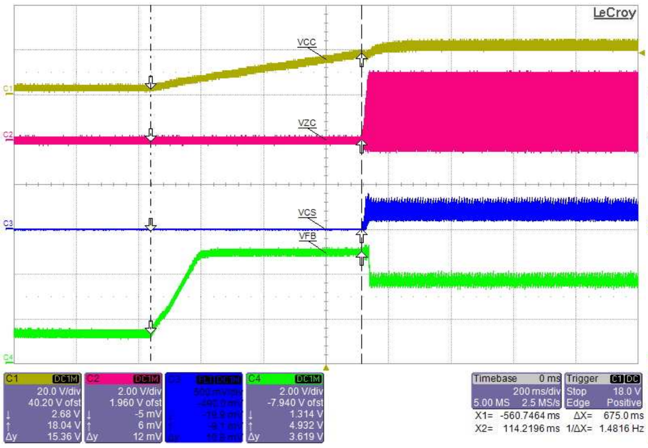


Figure 10: Constant Charging VCC at Startup

CH1 Supply Voltage, VCC

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Feedback Voltage, VFB

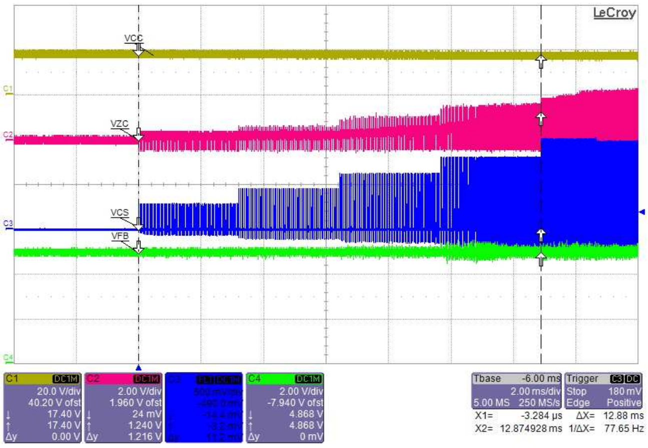


Figure 11: 4 Steps Softstart

CH1 Supply Voltage, VCC

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Feedback Voltage, VFB

12.2 Zero Crossing Point During Normal Operation

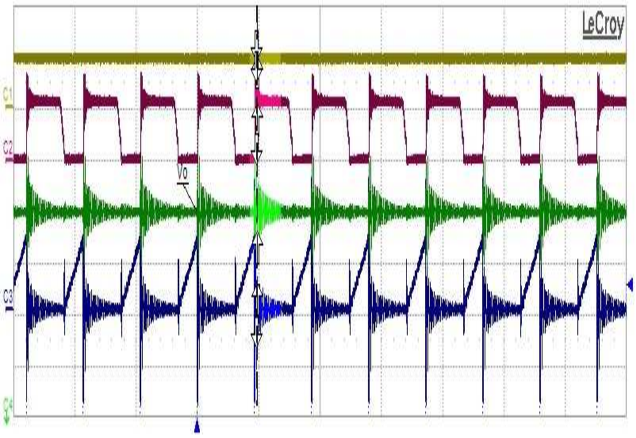


Figure 12: Working at 1st ZC

CH1 Supply Voltage, VCC

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Feedback Voltage, VFB

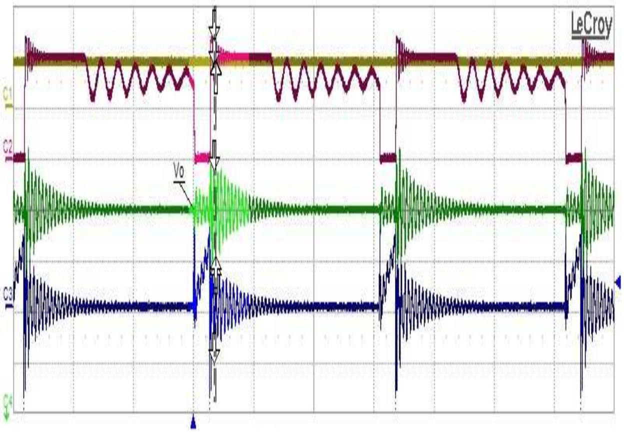


Figure 13: Working at 7th ZC

CH1 Supply Voltage, VCC

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Feedback Voltage, VFB

12.3 Load Transient Response

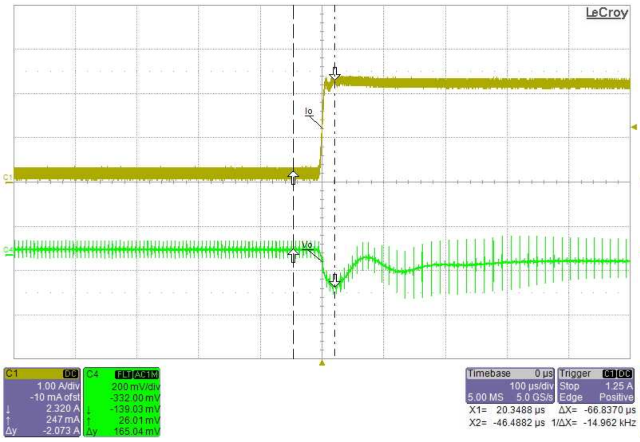


Figure 14: AC Output Ripple undershoot

CH1 Output Current, Io

CH4 Output Voltage, Vo

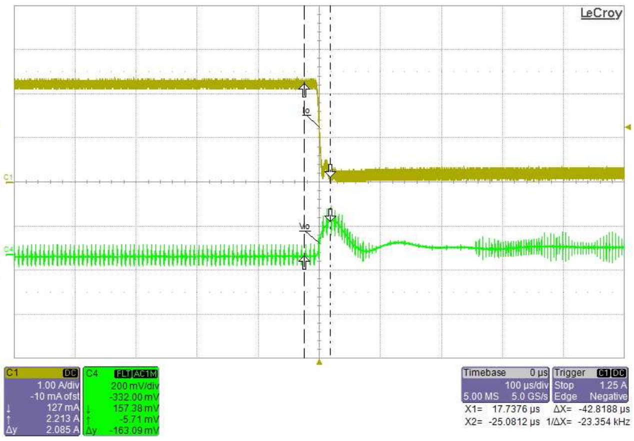


Figure 15: AC Output Ripple Overshoot

CH1 Output Current, Io

CH4 Output Voltage, Vo

12.4 Burst Mode Operation

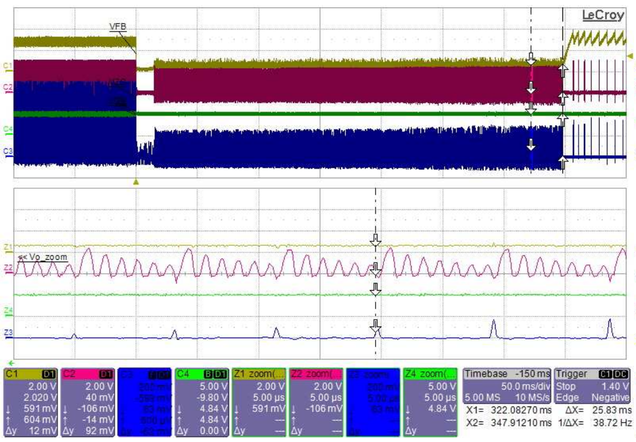


Figure 16: Entering Burst Mode

CH1 Feedback Voltage, VFB

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Output Voltage, Vo

Condition: ZC=7, FB<1.2V, Blanking time =30ms

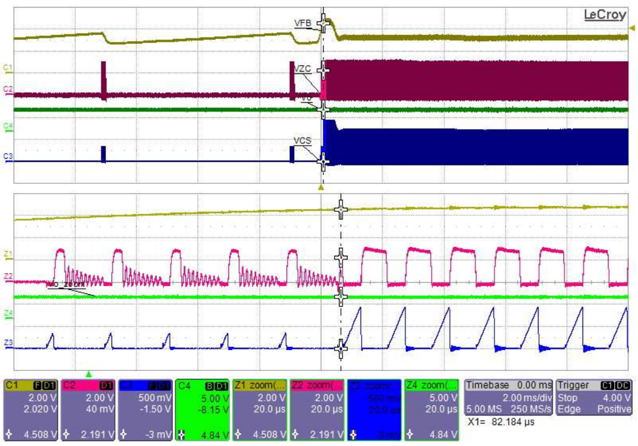


Figure 17: Leaving Burst Mode

CH1 Feedback Voltage, VFB

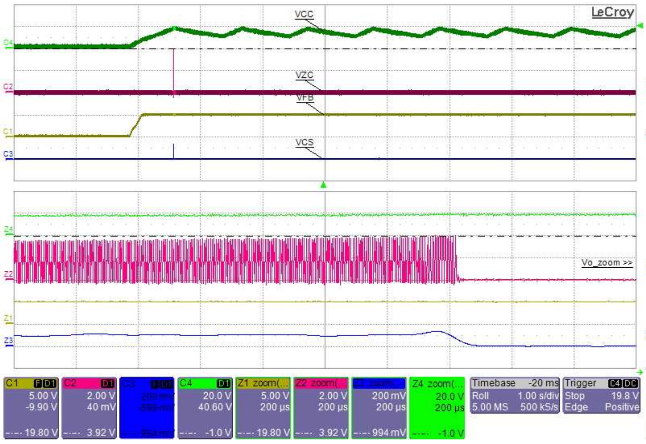
CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Output Voltage, Vo

Condition: VFB>4.5V

12.5 Protection Mode



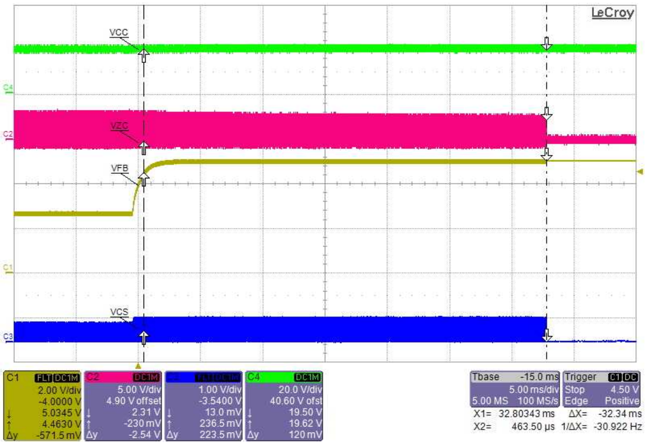


Figure 16: Over ZC Latch

CH1 Feedback Voltage, VFB

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Supply Voltage, VCC

Condition: VZC > 3.7V

Figure 17: Over Load/ Open Loop Protection

CH1 Feedback Voltage, VFB

CH2 Zero Crossing Voltage, VZC

CH3 Current Sense Voltage, VCS

CH4 Supply Voltage, VCC

Condition: VFB > 4.5V for 30ms

13 References

[1] ICE2QR4780Z datasheet, Infineon Technologies AG, 2010

[2] Converter Design Using the Quasi-Resonant PWM Controller ICE2QS01, Infineon Technologies AG, 2006. [ANPS0003]

[3] Design tips for flyback converters using the Quasi-Resonant PWM controller ICE2QS01, Infineon Technologies, 2006. [ANPS0005]

[4] Determine the switching frequency of Quasi-Resonant flybacl converters designed with ICE2QS01, Infineon Technologies, 2006. [ANPS0004]

[5] ICE2QRXX65/80X Quasi Resonance Coolset Design Guide. [ANPS0053]